Chapter 8 Microwave filters

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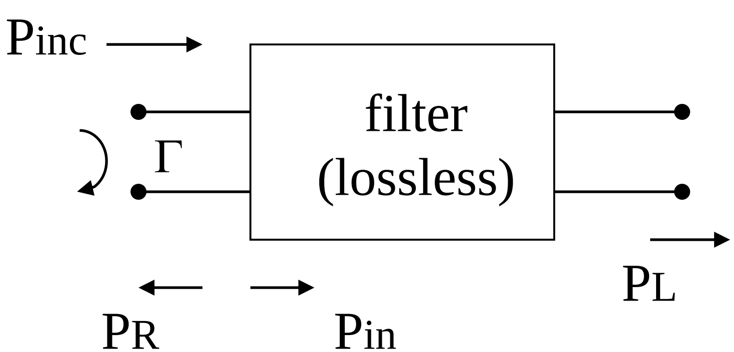
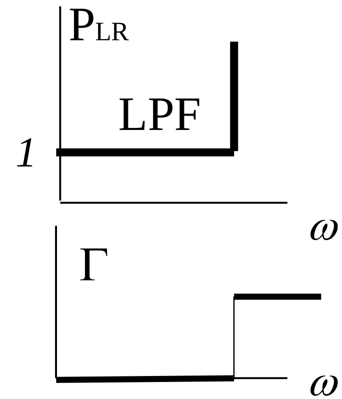
8.3 Filter design by the insertion loss method

- Power loss ratio (insertion loss)

$$P_{LR} \equiv \frac{P_{inc}}{P_L} = \frac{P_{inc}}{P_{inc} - P_R} = \frac{1}{1-|\Gamma(\omega)|^2} = \frac{1}{1-\frac{M(\omega^2)}{M(\omega^2)+N(\omega^2)}} = 1 + \frac{M(\omega^2)}{N(\omega^2)}$$





<u>Discussion</u>

1. $P_{inc} (= P_{avs}$, available power from source$) = P_{in} + P_R$

$P_{in} = P_L$ for a lossless filter

insertion loss $IL \equiv 10 \log P_{LR} = 10 \log \frac{P_{inc}}{P_L}$ $(= -10 \log G_T)$ (12.13)

$(= -20 \log |S_{21}|$, if $\Gamma_S = \Gamma_L = 0)$

return loss $RL \equiv 10 \log \frac{P_{inc}}{P_R} = -20 \log |\Gamma|$

2. $|\Gamma(w)|^2$ is an even function of w $\rightarrow |\Gamma(w)|^2 = \dfrac{M(w^2)}{M(w^2)+N(w^2)}$ (p.173)

$\because v(t): \text{real} \rightarrow \text{Re}V(w): even, \text{Im}V(w): odd \rightarrow V(-w) = V^*(w)$

$I(-w) = I^*(w), Z(-w) = Z^*(w), \Gamma(-w) = \Gamma^*(w)$

$|\Gamma(w)|^2 = \Gamma(w)\Gamma^*(w) = \Gamma(w)\Gamma(-w), |\Gamma(-w)|^2 = \Gamma(-w)\Gamma^*(-w) = \Gamma(-w)\Gamma(w)$

3. Maximally flat (Butterworth, binomial) LPF

$P_{LR}(w) = 1 + \varepsilon(\dfrac{w}{w_c})^{2N}, w_c$:cutoff frequency, $\varepsilon = 1 \rightarrow P_{LR}(w_c) = 2 = 3dB$

stopband attenuation $20NdB/decade$

4. Equal ripple (Chebyshev, optimal) LPF

$P_{LR}(w) = 1 + \varepsilon T_N^2(\dfrac{w}{w_c})^{2N}, P_{LR}(w_c) = 1 + \varepsilon$

ripple $10^{\log(1+\varepsilon)}$ in passband, stopband attenuation $20NdB/decade$

frequency responses (p.400, Fig. 8.21)

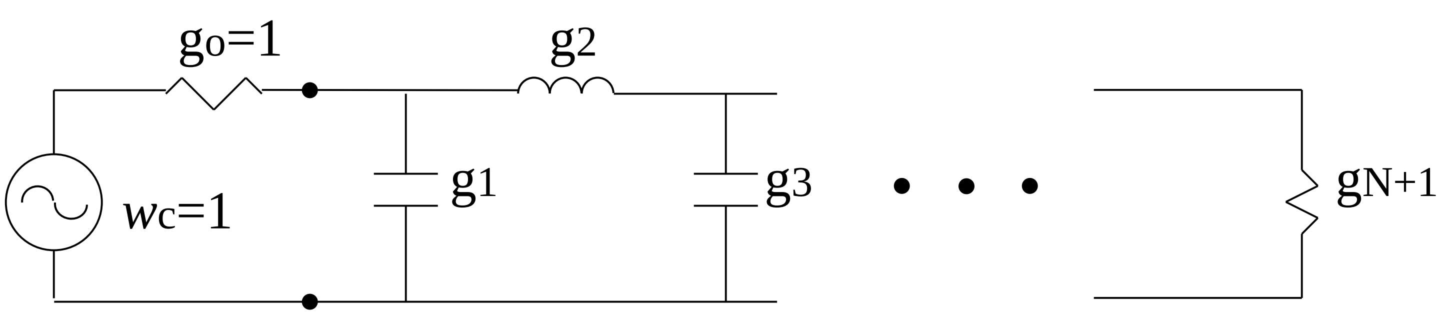
5. Filter design procedure:

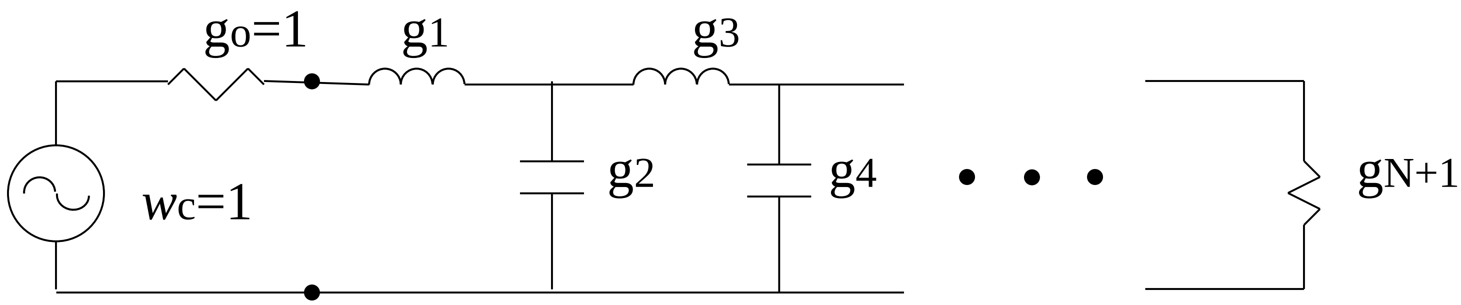
specification → LPF prototype → LPF, HPF, BPF, or BSF transformation → microstrip realization

6. Filter specification:

frequency range, BW, IL, stopband attenuation and frequencies, input and output impedances, VSWR, group delay, phase linearity, temperature range, and transient response.

- LPF prototype





Discussion

1. Maximally flat LPF prototype design equations

$$IL = 10\log[1+(\frac{w}{w_c})^{2N}]$$

$$w_c = 1, g_o = g_{N+1} = 1, g_k = 2\sin\frac{(2k-1)\pi}{2N} \quad k = 1,2,\ldots N$$

$$N = \frac{\log(10^{IL(w)/10} - 1)}{2\log\frac{w}{w_c}}$$

2. Element values for maximally flat LPF prototype are given in Table 8.3 of p.404, frequency response given in Fig. 8.26 of p.405.

3. Equal-ripple LPF prototype design equations

$$IL = 10\log[1+\varepsilon T_N^2(\frac{w}{w_c})]$$

$$\varepsilon = 10^{\frac{ripple(dB)}{10}} - 1$$

$$T_N(w) = \begin{cases} \cos(N\cos^{-1}\frac{w}{w_c}) & 0 \le w \le w_c \\ \cosh(N\cosh^{-1}\frac{w}{w_c}) & w > w_c \end{cases}$$

$$N = \frac{\cosh^{-1}[10^{IL(w)/10} - 1]/[10^{\frac{ripple(dB)}{10}} - 1]}{\cos^{-1}(\frac{w}{w_c})}$$

$$w_c = 1,\ g_o = 1,\ g_1 = \frac{2a_1}{\gamma},\ g_{N+1} = \begin{cases} 1, & N\ odd \\ \coth^2 \dfrac{\beta}{4}, & N\ even \end{cases}$$

$$\gamma = \sinh \frac{\beta}{2N}$$

$$\beta = \ln[\coth \frac{10\log(\varepsilon + 1)}{17.37}]$$

$$g_k = \frac{4a_{k-1}a_k}{b_{k-1}b_k},\ k = 2,3,\ldots N$$

$$a_k = \sin\frac{(2k-1)\pi}{2N},\ b_k = \gamma^2 + \sin^2\frac{k\pi}{N},\ k = 1,2,\ldots N$$

4. Element values for equal-ripple LPF prototype (p.406, Table 8.4) and frequency response (p.407, Fig. 8.27)

TABLE 8.3 Element Values for Maximally Flat Low-Pass Filter Prototypes ($g_0 = 1$, $\omega_c = 1$, $N = 1$ to 10)

N	g_1	g_2	g_3	g_4	g_5	g_6	g_7	g_8	g_9	g_{10}	g_{11}
1	2.0000	1.0000									
2	1.4142	1.4142	1.0000								
3	1.0000	2.0000	1.0000	1.0000							
4	0.7654	1.8478	1.8478	0.7654	1.0000						
5	0.6180	1.6180	2.0000	1.6180	0.6180	1.0000					
6	0.5176	1.4142	1.9318	1.9318	1.4142	0.5176	1.0000				
7	0.4450	1.2470	1.8019	2.0000	1.8019	1.2470	0.4450	1.0000			
8	0.3902	1.1111	1.6629	1.9615	1.9615	1.6629	1.1111	0.3902	1.0000		
9	0.3473	1.0000	1.5321	1.8794	2.0000	1.8794	1.5321	1.0000	0.3473	1.0000	
10	0.3129	0.9080	1.4142	1.7820	1.9754	1.9754	1.7820	1.4142	0.9080	0.3129	1.0000

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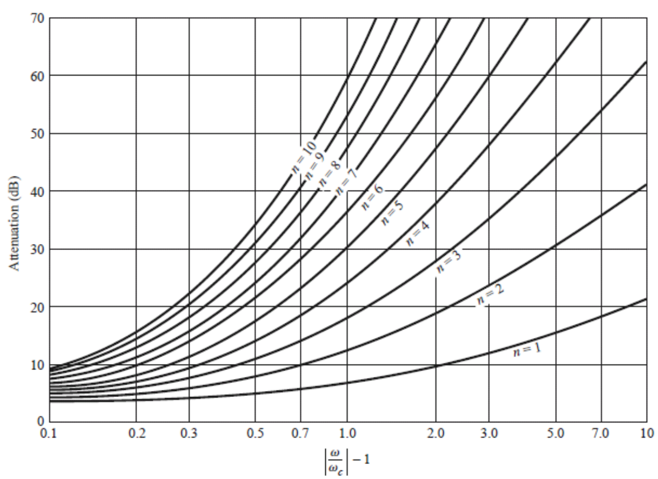

FIGURE 8.26 Attenuation versus normalized frequency for maximally flat filter prototypes.

Adapted from G. L. Matthaei, L. Young, and E. M. T. Jones, *Microwave Filters, Impedance-Matching Networks, and Coupling Structures*, Artech House, Dedham, Mass., 1980, with permission.

TABLE 8.4 Element Values for Equal-Ripple Low-Pass Filter Prototypes ($g_0 = 1, \omega_c = 1, N = 1$ to 10, 0.5 dB and 3.0 dB ripple)

					0.5 dB Ripple						
N	g_1	g_2	g_3	g_4	g_5	g_6	g_7	g_8	g_9	g_{10}	g_{11}
1	0.6986	1.0000									
2	1.4029	0.7071	1.9841								
3	1.5963	1.0967	1.5963	1.0000							
4	1.6703	1.1926	2.3661	0.8419	1.9841						
5	1.7058	1.2296	2.5408	1.2296	1.7058	1.0000					
6	1.7254	1.2479	2.6064	1.3137	2.4758	0.8696	1.9841				
7	1.7372	1.2583	2.6381	1.3444	2.6381	1.2583	1.7372	1.0000			
8	1.7451	1.2647	2.6564	1.3590	2.6964	1.3389	2.5093	0.8796	1.9841		
9	1.7504	1.2690	2.6678	1.3673	2.7239	1.3673	2.6678	1.2690	1.7504	1.0000	
10	1.7543	1.2721	2.6754	1.3725	2.7392	1.3806	2.7231	1.3485	2.5239	0.8842	1.9841

					3.0 dB Ripple						
N	g_1	g_2	g_3	g_4	g_5	g_6	g_7	g_8	g_9	g_{10}	g_{11}
1	1.9953	1.0000									
2	3.1013	0.5339	5.8095								
3	3.3487	0.7117	3.3487	1.0000							
4	3.4389	0.7483	4.3471	0.5920	5.8095						
5	3.4817	0.7618	4.5381	0.7618	3.4817	1.0000					
6	3.5045	0.7685	4.6061	0.7929	4.4641	0.6033	5.8095				
7	3.5182	0.7723	4.6386	0.8039	4.6386	0.7723	3.5182	1.0000			
8	3.5277	0.7745	4.6575	0.8089	4.6990	0.8018	4.4990	0.6073	5.8095		
9	3.5340	0.7760	4.6692	0.8118	4.7272	0.8118	4.6692	0.7760	3.5340	1.0000	
10	3.5384	0.7771	4.6768	0.8136	4.7425	0.8164	4.7260	0.8051	4.5142	0.6091	5.8095

Source: Reprinted from G. L. Matthaei, L. Young, and E. M. T. Jones, *Microwave Filters, Impedance-Matching Networks, and Coupling Structures*, Artech House, Dedham, Mass.,1980, with permission.

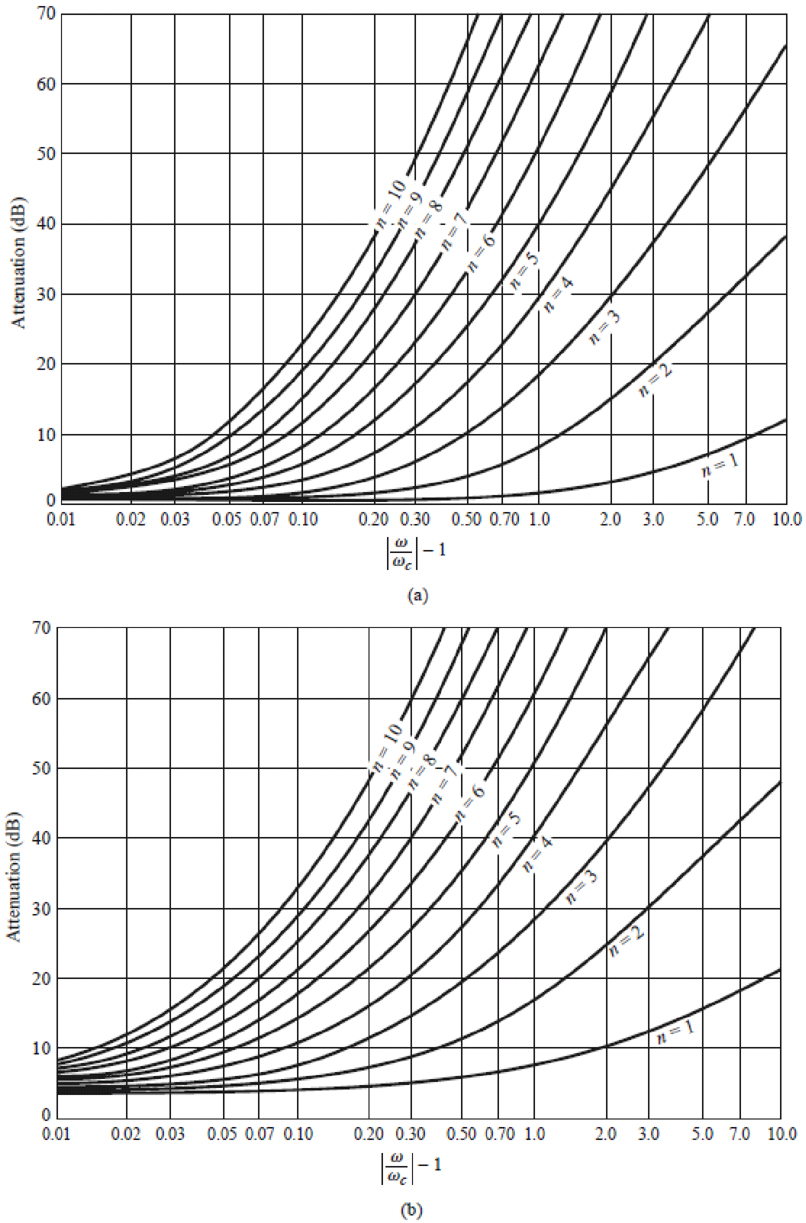

FIGURE 8.27 Attenuation versus normalized frequency for equal-ripple filter prototypes (a) 0.5 dB ripple level. (b) 3.0 dB ripple level.

TABLE 8.5 Element Values for Maximally Flat Time Delay Low-Pass Filter Prototypes ($g_0 = 1, \omega_c = 1, N = 1$ to 10)

N	g_1	g_2	g_3	g_4	g_5	g_6	g_7	g_8	g_9	g_{10}	g_{11}
1	2.0000	1.0000									
2	1.5774	0.4226	1.0000								
3	1.2550	0.5528	0.1922	1.0000							
4	1.0598	0.5116	0.3181	0.1104	1.0000						
5	0.9303	0.4577	0.3312	0.2090	0.0718	1.0000					
6	0.8377	0.4116	0.3158	0.2364	0.1480	0.0505	1.0000				
7	0.7677	0.3744	0.2944	0.2378	0.1778	0.1104	0.0375	1.0000			
8	0.7125	0.3446	0.2735	0.2297	0.1867	0.1387	0.0855	0.0289	1.0000		
9	0.6678	0.3203	0.2547	0.2184	0.1859	0.1506	0.1111	0.0682	0.0230	1.0000	
10	0.6305	0.3002	0.2384	0.2066	0.1808	0.1539	0.1240	0.0911	0.0557	0.0187	1.0000

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8.4 Filter transformations

- Impedance scaling $g_o = 1 \rightarrow R_o \Rightarrow impedance \times R_o$

  scaled values: $R_S' = R_o, R_L' = R_o R_L, L' = R_o L, C' = \dfrac{C}{R_o}$

- Frequency scaling

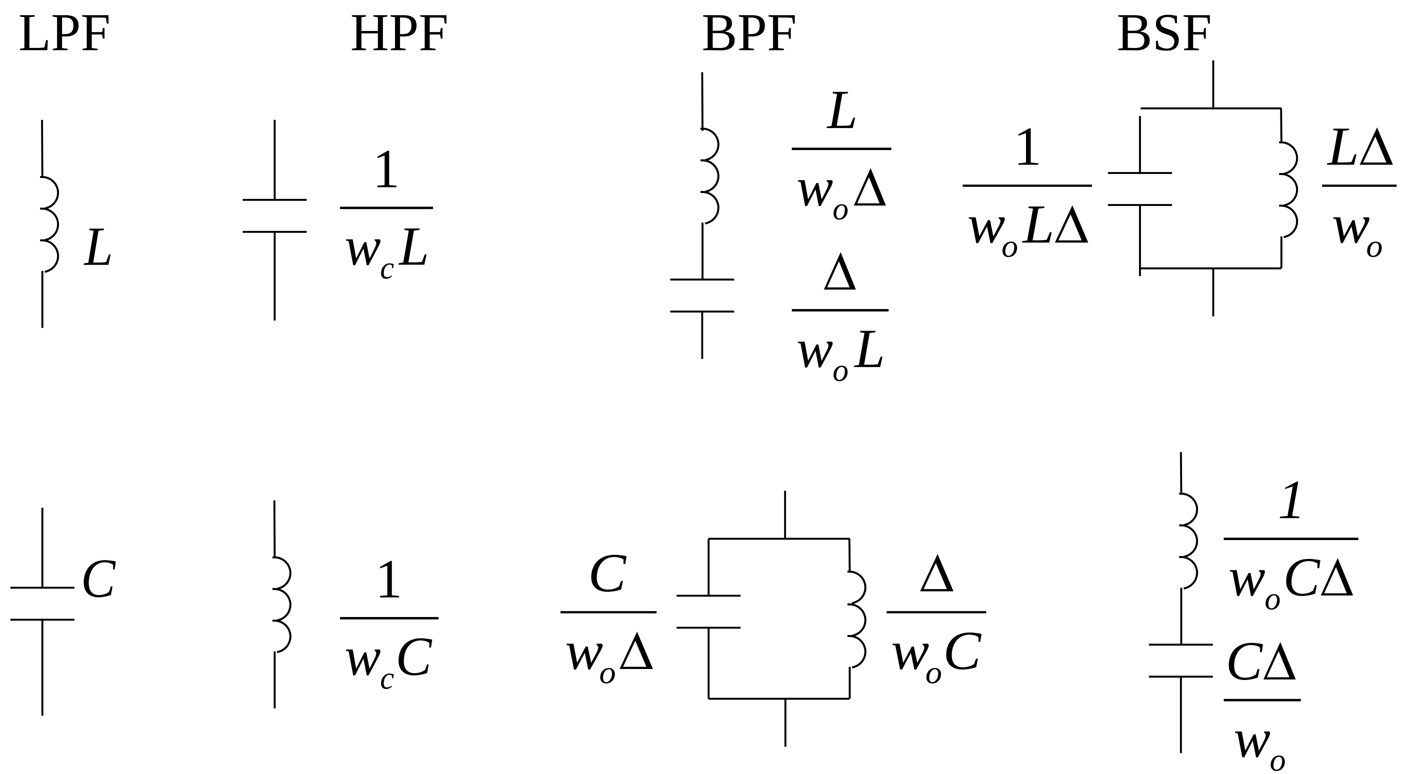
  $w: 1 \rightarrow w_c \Rightarrow P'_{LR}(w) = P_{LR}(\dfrac{w}{w_c}) \Rightarrow$ same impedance, $w \leftarrow \dfrac{w}{w_c}$

  scaled values:
  $$jX_L = j\frac{w}{w_c}L = jwL' \rightarrow L' = \frac{L}{w_c}$$
  $$jB_C = j\frac{w}{w_c}C = jwC' \rightarrow C' = \frac{C}{w_c}$$

- Impedance and frequency scaling

  scaled values: $R_S' = R_o, R_L' = R_o R_L, L' = \dfrac{R_o L}{w_c}, C' = \dfrac{C}{R_o w_c}$

- Frequency scaling for HPF, BPF and BSF



$$\Delta = \frac{w_2 - w_1}{w_o} \text{ : fractional BW}$$

Discussion

1. Ex. 8.3 design a maximally flat LPF, fc=2GHz, Zo=50Ω, IL(3GHz) =15dB

from Fig.8.26, $IL = 15dB$ for $\left|\frac{w}{w_c}\right| - 1 = 0.5 @ 3GHz \rightarrow N = 5$

from Table 8.3, $C_1 = C_5 = 0.618, L_2 = L_4 = 1.618, C_3 = 2$

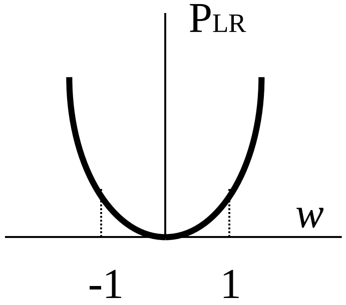
$$\rightarrow C_1' = C_5' = \frac{C_1}{50w_c} = 0.984pF$$

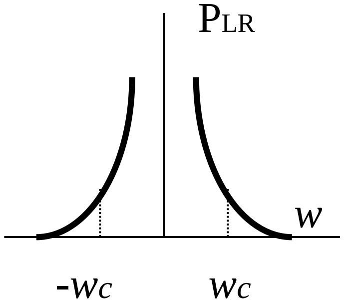
$$L_2' = L_4' = \frac{50L_2}{w_c} = 6.438nH$$

$$C_3' == \frac{C_3}{50w_c} = 3.183pF$$

frequency response (p.412, Fig. 8.30) with the comparison of equal-ripple LPF and linear phase LPF

2. LPF $\rightarrow$ HPF frequency scaling





$$0 \rightarrow \pm\infty, 1 \rightarrow -w_c, -1 \rightarrow w_c \Rightarrow \quad w \leftarrow -\frac{w_c}{w}$$

$$LPF \begin{cases} \dfrac{1}{jwC} \rightarrow \dfrac{1}{-j\dfrac{w_c C}{w}} = jwL' \\ jwL \rightarrow -j\dfrac{w_c L}{w} = \dfrac{1}{jwC'} \end{cases} \Rightarrow HPF \begin{cases} L' = \dfrac{1}{w_c C} \\ C' = \dfrac{1}{w_c L} \end{cases}$$

3. LPF $\rightarrow$ BPF frequency scaling

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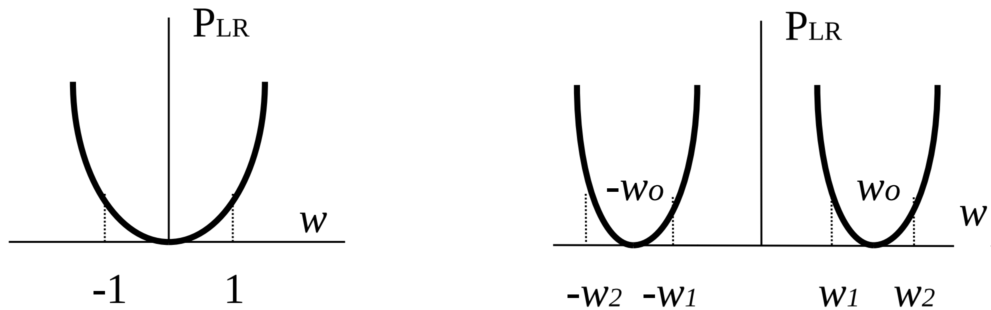

$$0 \rightarrow w_o, 1 \rightarrow w_2, -1 \rightarrow w_1 \Rightarrow \quad w \leftarrow \frac{1}{\Delta}\left(\frac{w}{w_o} - \frac{w_o}{w}\right),\ w_o = \sqrt{w_1 w_2}, \Delta = \frac{w_2 - w_1}{w_o}$$

$$LPF \begin{cases} \dfrac{1}{jwC} \rightarrow \dfrac{1}{j\dfrac{C}{\Delta}\left(\dfrac{w}{w_o} - \dfrac{w_o}{w}\right)} = \dfrac{1}{jw\dfrac{C}{w_o\Delta} + \dfrac{Cw_o}{jw\Delta}} \\ jwL \rightarrow j\dfrac{L}{\Delta}\left(\dfrac{w}{w_o} - \dfrac{w_o}{w}\right) = jw\dfrac{L}{w_o\Delta} + \dfrac{Lw_o}{jw\Delta} \end{cases} \Rightarrow BPF \begin{cases} C' = \dfrac{C}{w_o\Delta}, L' = \dfrac{\Delta}{w_o C} \\ L' = \dfrac{L}{w_o\Delta}, C' = \dfrac{\Delta}{w_o L} \end{cases}$$

4. LPF $\rightarrow$ BSF frequency scaling

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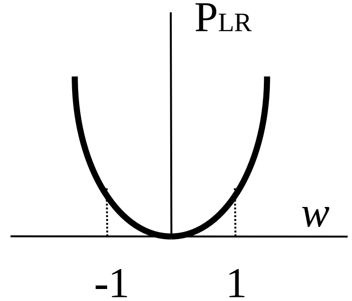
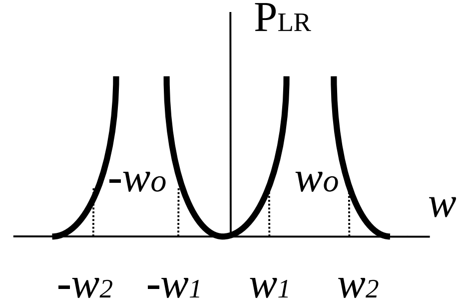




$$0 \rightarrow \pm\infty, 1 \rightarrow -w_1, -1 \rightarrow w_2 \Rightarrow \quad w \leftarrow \frac{\Delta}{\frac{w_o}{w} - \frac{w}{w_o}}$$

$$LPF \begin{cases} \frac{1}{jwC} \rightarrow \frac{1}{jC(\frac{\Delta}{\frac{w_o}{w} - \frac{w}{w_o}})} = \frac{w_o}{jwC\Delta} + \frac{jw}{C\Delta w_o} \\ jwL \rightarrow jL(\frac{\Delta}{\frac{w_o}{w} - \frac{w}{w_o}}) = \frac{1}{\frac{w_o}{jwL\Delta} + \frac{jw}{Lw_o\Delta}} \end{cases} \Rightarrow BSF \begin{cases} C' = \frac{C\Delta}{w_o}, L' = \frac{1}{w_o C\Delta} \\ L' = \frac{L\Delta}{w_o}, C' = \frac{1}{w_o L\Delta} \end{cases}$$

5. Ex. 8.4 design a N=3, 0.5dB equal-ripple BPF, f_o=1GHz, Z_o=50Ω, BW=10%

from Table 8.4, $L_1 = L_3 = 1.5963, C_2 = 1.0967, R_L = 1$

$$\rightarrow L_1' = L_3' = \frac{L_1 50}{w_o \Delta} = 127nH$$

$$C_1' = C_3' = \frac{\Delta}{w_o L_1 50} = 0.199\,pF$$

$$L_2' = \frac{50\Delta}{w_o C_2} = 0.726nH$$

$$C_2' == \frac{C_2}{50 w_o \Delta} = 34.91pF$$

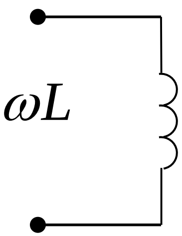
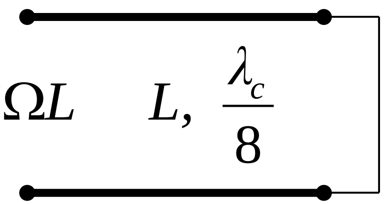
frequency response (p.415, Fig. 8.33)

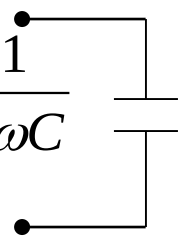
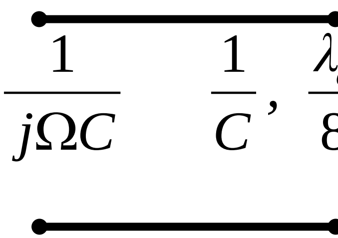
8.5 Filter implementation

• Richards' transformation

$\omega \rightarrow \Omega$, $\Omega \equiv \tan\beta l = \tan(\omega l / v_p)$

lumped elements → commensurate lines with S.C. or O.C. stub

$Z_{in} = j\omega L$  L → $Z_{in} = j\Omega L$  $L, \dfrac{\lambda_c}{8}$

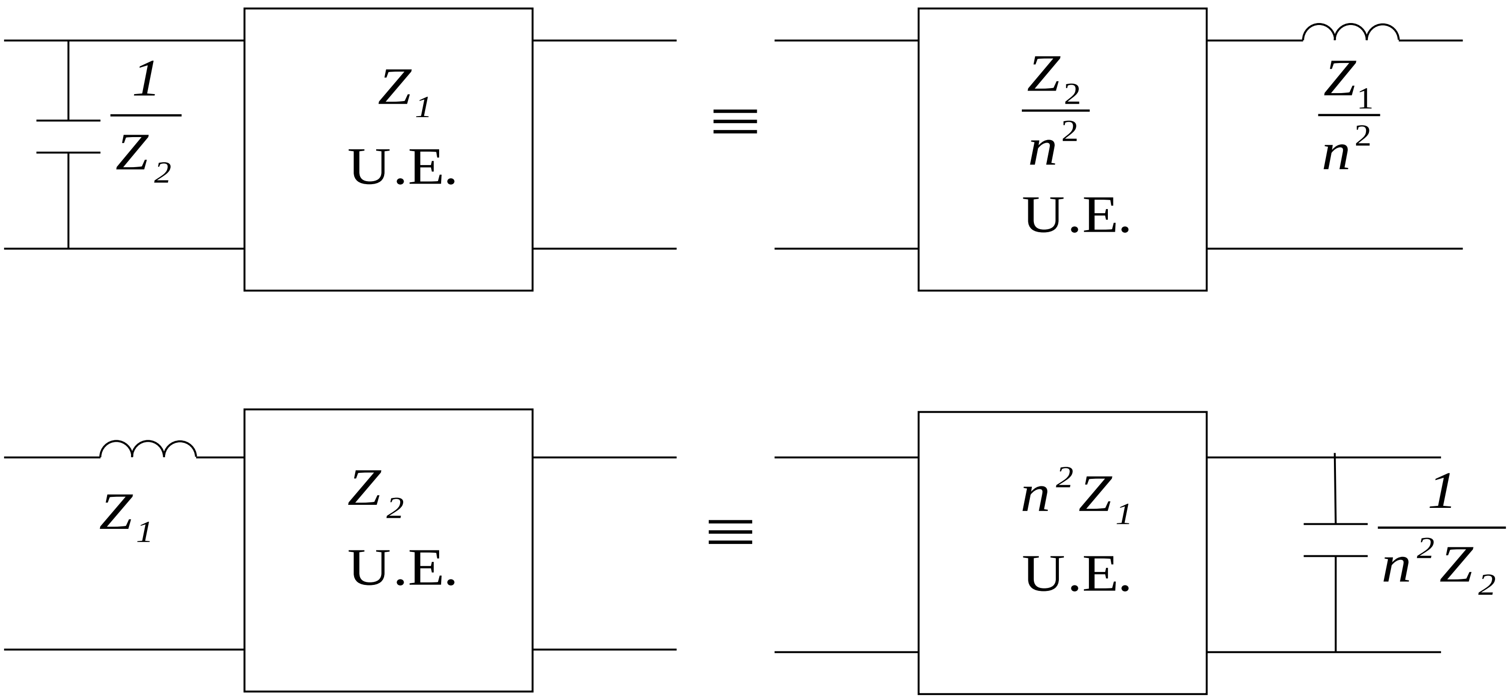
$Z_{in} = \dfrac{1}{j\omega C}$  C → $Z_{in} = \dfrac{1}{j\Omega C}$  $\dfrac{1}{C}, \dfrac{\lambda_c}{8}$

<u>Discussion</u>

1. $\omega_c = 1 \rightarrow \Omega_c = \tan\beta_c l = \tan\dfrac{2\pi}{\lambda_c}\dfrac{\lambda_c}{8} = \tan\dfrac{\pi}{4} = 1$

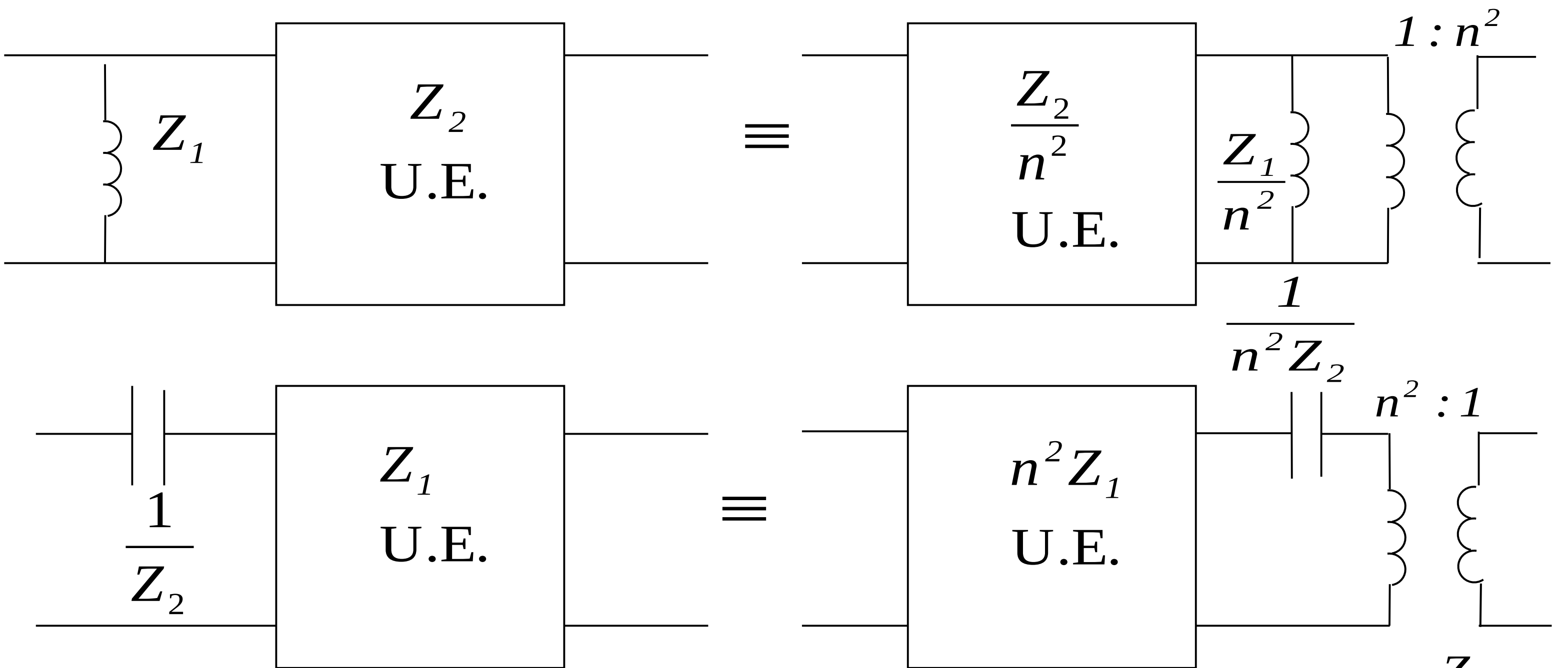
2. $\beta\dfrac{\lambda_c}{8} = \pi \rightarrow \dfrac{\omega}{c}\dfrac{\lambda_c}{8} = \pi \rightarrow \omega = 8\pi f_c = 4\omega_c \Rightarrow$ stub response repeats every $4\omega_c$.

- Kuroda's identites



$$n^2 = 1 + \frac{Z_2}{Z_1}$$

U.E. (unit element) : $\lambda_c/8$ line

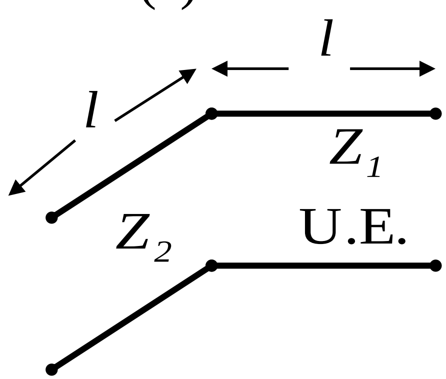


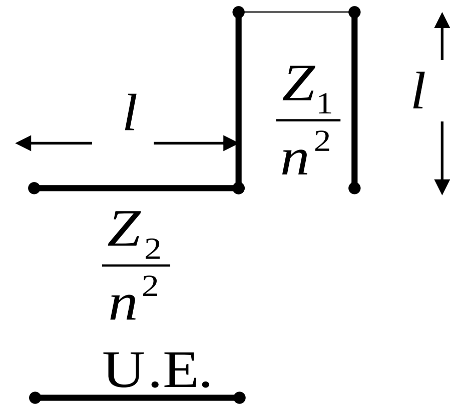
$$n^2 = 1 + \frac{Z_2}{Z_1}$$

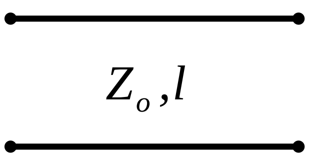
Discussion

1. Use $\lambda_c/8$ redundant lines to separate stubs.
2. series L (short stub) ↔ shunt C (open stub)
   series C and shunt L change positions

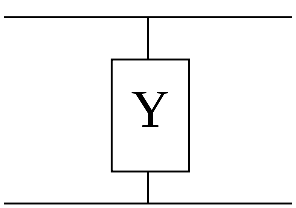
3. derivation of (a)



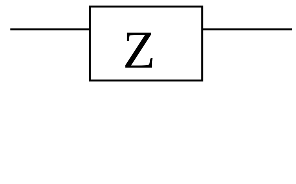




$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} \cos\beta l & jZ_o \sin\beta l \\ jY_o \sin\beta l & \cos\beta l \end{bmatrix} = \frac{1}{\sqrt{1+\Omega^2}} \begin{bmatrix} 1 & j\Omega Z_o \\ \frac{j\Omega}{Z_o} & 1 \end{bmatrix}$$



$$\begin{bmatrix} 1 & 0 \\ Y & 1 \end{bmatrix} = \begin{cases} \begin{bmatrix} 1 & 0 \\ \frac{j\Omega}{Z_o} & 1 \end{bmatrix} & \text{open-circuited shunt stub} \\ \begin{bmatrix} 1 & 0 \\ \frac{1}{j\Omega Z_o} & 1 \end{bmatrix} & \text{short-circuited shunt stub} \end{cases}$$



$$\begin{bmatrix} 1 & Z \\ 0 & 1 \end{bmatrix} = \begin{cases} \begin{bmatrix} 1 & \dfrac{Z_o}{j\Omega} \\ 0 & 1 \end{bmatrix} \text{ open-circuited series stub} \\ \begin{bmatrix} 1 & j\Omega\, Z_o \\ 0 & 1 \end{bmatrix} \text{short-circuited series stub} \end{cases}$$

$$\begin{bmatrix} A & B \\ C & D \end{bmatrix}_L = \frac{1}{\sqrt{1+\Omega^2}} \begin{bmatrix} 1 & 0 \\ \dfrac{j\Omega}{Z_2} & 1 \end{bmatrix} \begin{bmatrix} 1 & j\Omega\, Z_1 \\ \dfrac{j\Omega}{Z_1} & 1 \end{bmatrix}$$

$$= \frac{1}{\sqrt{1+\Omega^2}} \begin{bmatrix} 1 & j\Omega\, Z_1 \\ j\Omega\, (\dfrac{1}{Z_1} + \dfrac{1}{Z_2}) & 1 - \Omega^2 \dfrac{Z_1}{Z_2} \end{bmatrix}$$

$$\begin{bmatrix} A & B \\ C & D \end{bmatrix}_R = \frac{1}{\sqrt{1+\Omega^2}} \begin{bmatrix} 1 & \dfrac{j\Omega Z_2}{n^2} \\ \dfrac{j\Omega\, n^2}{Z_2} & 1 \end{bmatrix} \begin{bmatrix} 1 & \dfrac{j\Omega Z_1}{n^2} \\ 0 & 1 \end{bmatrix}$$

$$= \frac{1}{\sqrt{1+\Omega^2}} \begin{bmatrix} 1 & \dfrac{j\Omega}{n^2}(Z_1 + Z_2) \\ \dfrac{j\Omega n^2}{Z_2} & 1 - \Omega^2 \dfrac{Z_1}{Z_2} \end{bmatrix} \rightarrow n^2 = 1 + \frac{Z_2}{Z_1}$$

4. Microstrp LPF design procedure

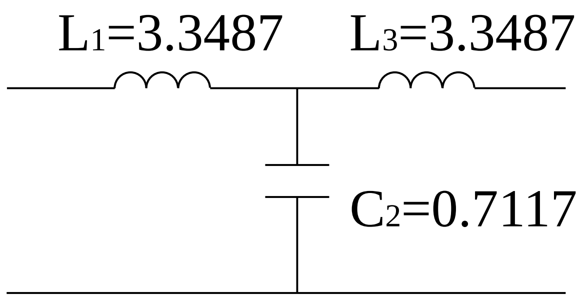
series L, shunt C → $\lambda_c/8$ series short stub, $\lambda_c/8$ shunt open stub

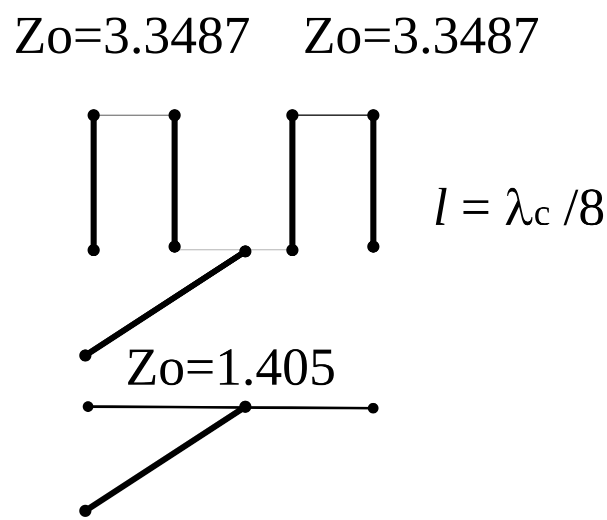
→ add redundant $\lambda_c/8$ Z_o lines → $\lambda_c/8$ shunt open stubs

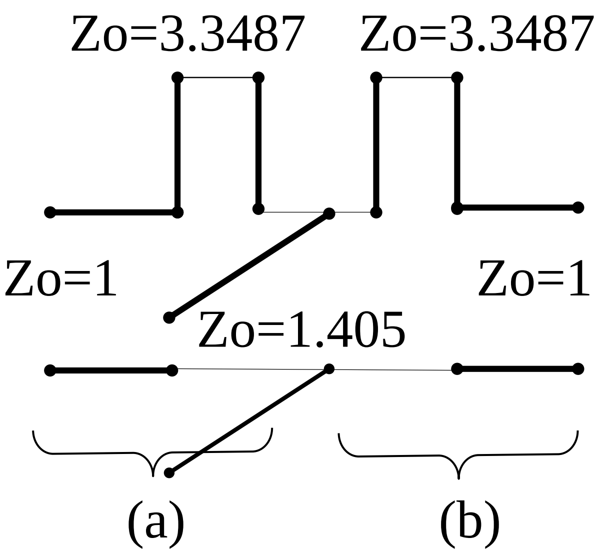
→ consider discontinuity effects

5. Ex.8.5 design a 3dB equal-ripple LPF with f_c=4GHz, N=3,

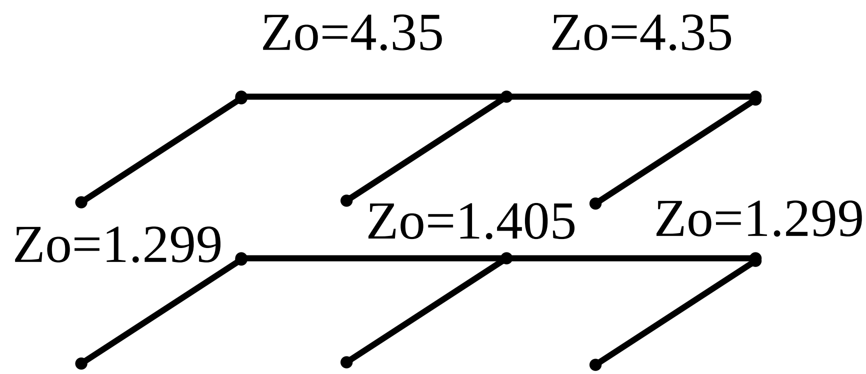
Zin, Zout=50Ω

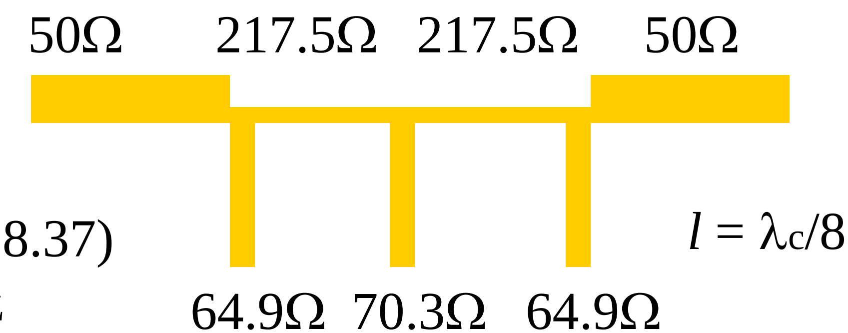






Kuroda’s identity



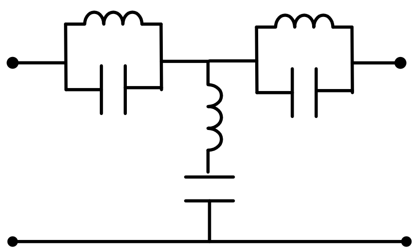


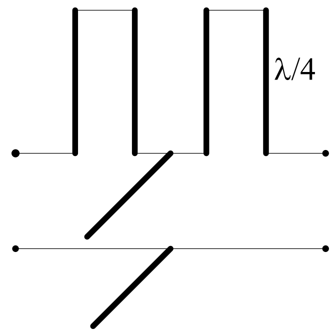
frequency response (p.421, Fig.8.37)

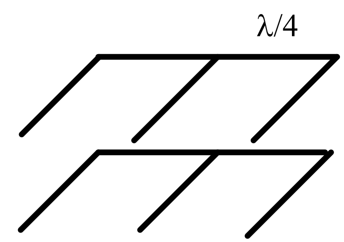
frequency repeats every 16GHz

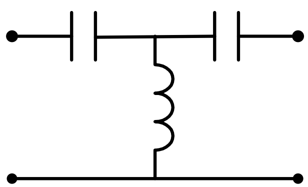
S_{21} @8GHz, 24GHz (l=λ’/4, 3λ’/4,…)

6. Similar procedures can be used for bandstop filters, but Kuroda identities are not useful for highpass or bandpass filters. (p.421)

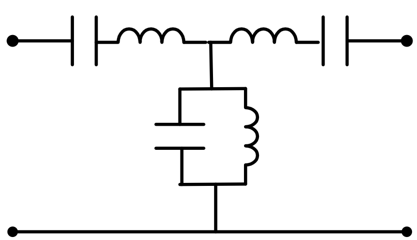


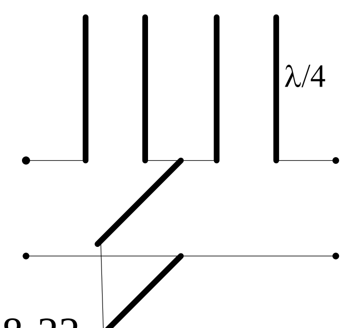






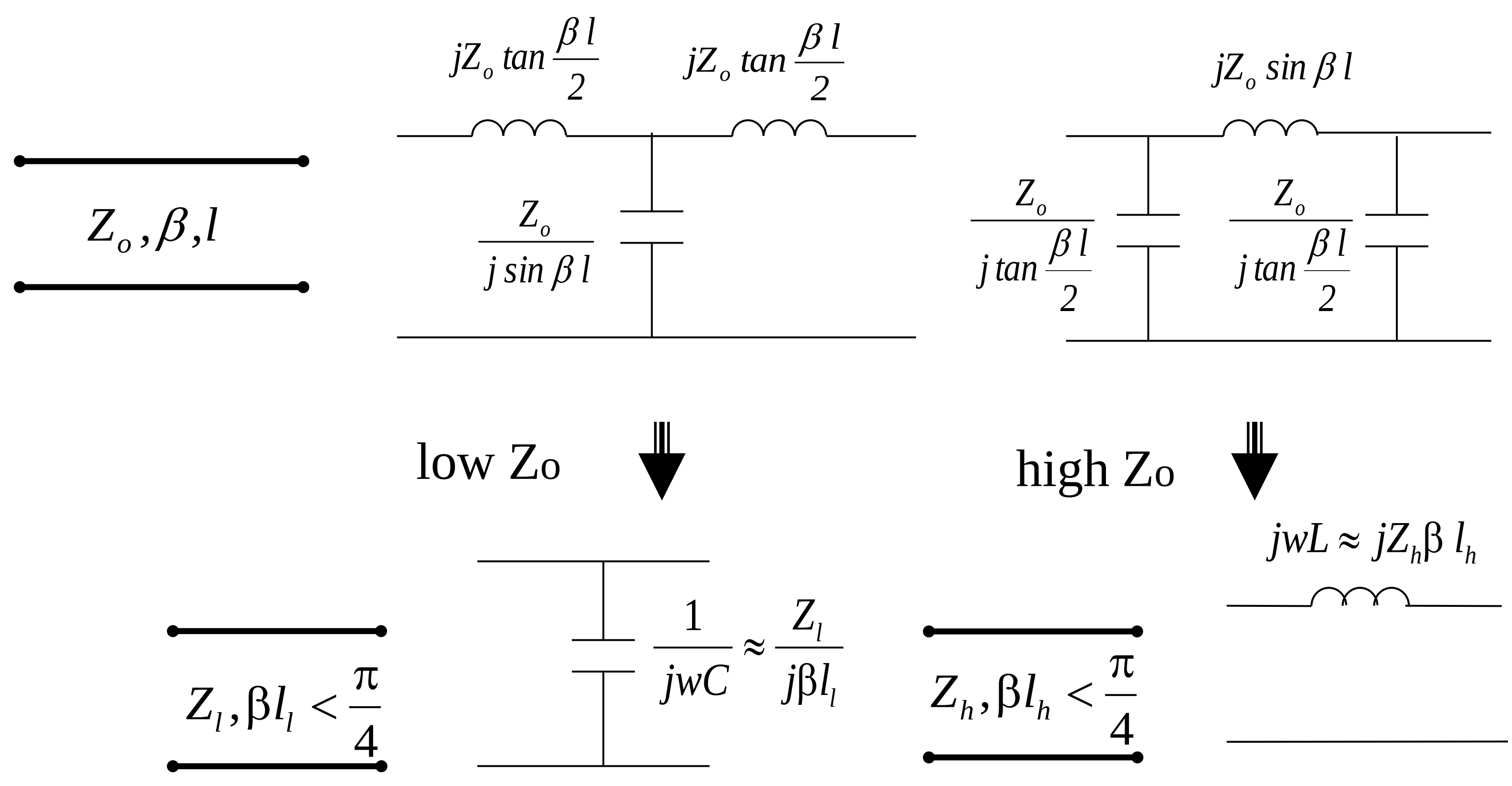
Series capacitor transformation is not available in Kuroda identities.





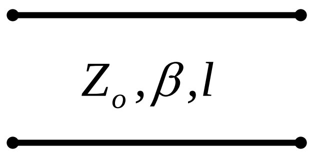
8.6 Stepped-impedance LPF

- Short transmission line section



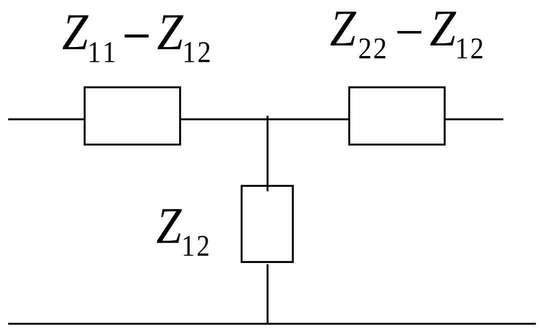
Discussion

1. (derivation from notes 4-12, 13)



$$\theta = \beta l$$

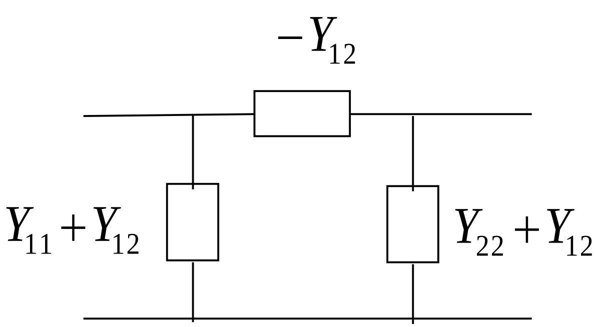
$$[Z] = -jZ_o\begin{bmatrix} \cot\theta & \csc\theta \\ \csc\theta & \cot\theta \end{bmatrix}, [Y] = -jY_o\begin{bmatrix} \cot\theta & -\csc\theta \\ -\csc\theta & \cot\theta \end{bmatrix}$$



$$Z_{12} = -jZ_o \csc\theta$$

$$Z_{11} - Z_{12} = -jZ_o(\cot\theta - \csc\theta) = -jZ_o\left(\frac{\cos\theta}{\sin\theta} - \frac{1}{\sin\theta}\right)$$

$$= -jZ_o \frac{-2\sin^2\frac{\theta}{2}}{2\sin\frac{\theta}{2}\cos\frac{\theta}{2}} = jZ_o \tan\frac{\theta}{2}$$



$$Y_{12} = jY_o \csc\theta$$

$$Y_{11} + Y_{12} = \frac{1}{jZ_o}\left[\frac{\cos\theta}{\sin\theta} - \frac{1}{\sin\theta}\right] = \frac{j\tan\frac{\theta}{2}}{Z_o}$$

2. Microstrp LPF design procedure

L, C $\rightarrow$ select proper Z_h, Z_l $\rightarrow$ at cutoff frequency $R_o L = Z_h \beta l_h$, $R_o/C = Z_l/\beta l_l$ $\rightarrow$ l_h, l_l $\rightarrow$ consider parasitics of L,C and discontinuity effects

3. Considerations of Z_l

$$\frac{Z_l}{j\sin\beta l_l} = \frac{1}{j\omega C} \rightarrow \sin\beta l_l = \omega C Z_l \overset{\beta l \le \frac{\pi}{4}}{\le} \frac{1}{\sqrt{2}} \rightarrow$$

$$Z_l \le \frac{1}{\omega C\sqrt{2}}$$

$$l_l = \frac{1}{\beta}\sin^{-1}\omega C Z_l \rightarrow \text{open stubs?}$$

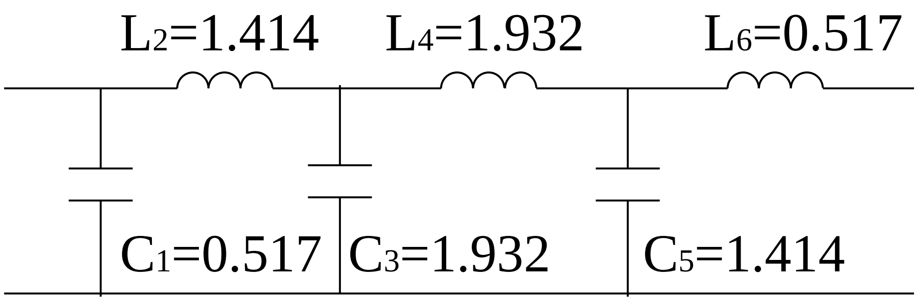
4. Considerations of Z_h

$$jZ_h \sin\beta l_h = j\omega L \rightarrow \sin\beta l_h = \frac{\omega L}{Z_h} \overset{\beta l \le \frac{\pi}{4}}{\le} \frac{1}{\sqrt{2}} \rightarrow$$

$$Z_h \ge \sqrt{2}\omega L \rightarrow \text{fabrication?}$$

$$l_h = \frac{1}{\beta}\sin^{-1}\frac{\omega L}{Z_h} \rightarrow \text{capacitor coupling?}$$

5. Ex.8.6 design a maximally flat LPF with f_c=2.5GHz, IL(4GHz)=20 dB, Z_{in}, Z_{out} =50Ω, Z_h=120Ω, Z_l =20Ω→N=6



$l_h = R_0 L/\beta Z_h$,

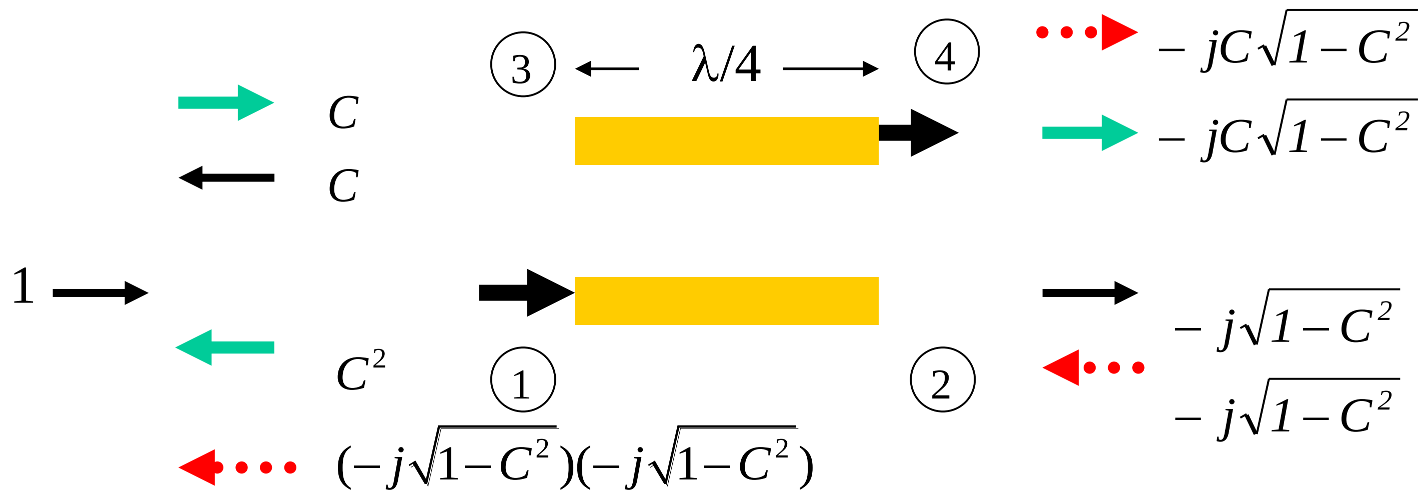
$l_l = C Z_l/\beta R_0$

frequency response (p.425, Fig.8.41)

no repetition of frequency response

8.7 Coupled line filters

- Coupled line BPF element



① $[C^2-(1-C^2)]^2 = 4C^4-4C^2+1$

④ $[-j2C\sqrt{1-C^2}]^2 = 4C^2(1-C^2) = -4C^4+4C^2$

① + ④ =1

if $C = \dfrac{1}{\sqrt{2}}, \rightarrow$ ① =0, ④ =1

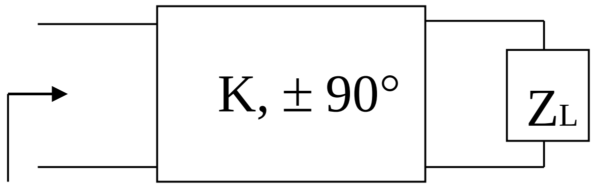
$$\begin{bmatrix} b_1 \\ b_2 \\ b_3 \\ b_4 \end{bmatrix} = \begin{bmatrix} 0 & -j\sqrt{1-C^2} & C & 0 \\ -j\sqrt{1-C^2} & 0 & 0 & C \\ C & 0 & 0 & -j\sqrt{1-C^2} \\ 0 & C & -j\sqrt{1-C^2} & 0 \end{bmatrix} \begin{bmatrix} a_1 \\ 0 \\ 0 \\ 0 \end{bmatrix} = \begin{bmatrix} 0 \\ -j\sqrt{1-C^2}a_1 \\ Ca_1 \\ 0 \end{bmatrix}$$

$$\begin{bmatrix} b_1 \\ b_2 \\ b_3 \\ b_4 \end{bmatrix} = \begin{bmatrix} 0 & -j\sqrt{1-C^2} & C & 0 \\ -j\sqrt{1-C^2} & 0 & 0 & C \\ C & 0 & 0 & -j\sqrt{1-C^2} \\ 0 & C & -j\sqrt{1-C^2} & 0 \end{bmatrix} \begin{bmatrix} 0 \\ -j\sqrt{1-C^2}a_1 \\ Ca_1 \\ 0 \end{bmatrix}$$

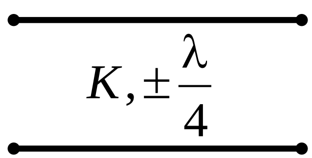
$$= \begin{bmatrix} [-(1-C^2)+C^2]a_1 \\ 0 \\ 0 \\ [-j\sqrt{1-C^2}C - j\sqrt{1-C^2}C]a_1 \end{bmatrix} \overset{C=\frac{1}{\sqrt{2}}}{=} \begin{bmatrix} 0 \\ 0 \\ 0 \\ -ja_1 \end{bmatrix}$$

• Impedance and admittance inverters (p.422, Fig. 8.38)

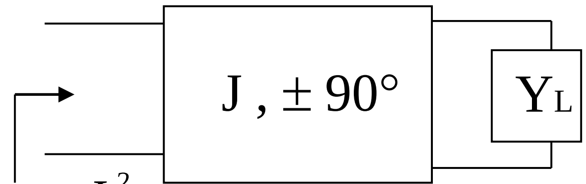
impedance inverter



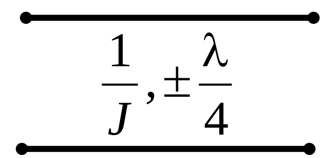
$$Z_{in} = \frac{K^2}{Z_L}$$

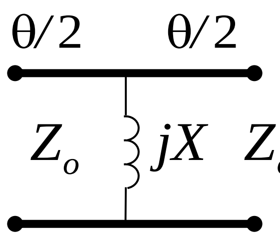


admittance inverter



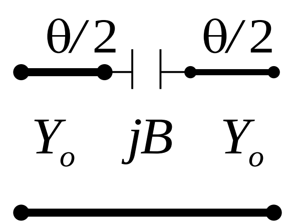
$$Y_{in} = \frac{J^2}{Y_L}$$





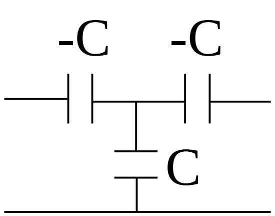
$$K = Z_o \tan\left|\frac{\theta}{2}\right|, X = \frac{K}{1-(\frac{K}{Z_o})^2}$$

$$\theta = -\tan^{-1}\frac{2X}{Z_o}$$

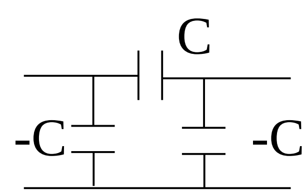


$$J = Y_o \tan\left|\frac{\theta}{2}\right|, B = \frac{J}{1-(\frac{J}{Y_o})^2}$$

$$\theta = -\tan^{-1}\frac{2B}{Y_o}$$

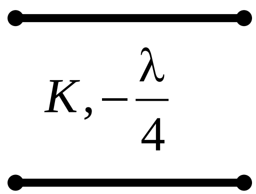


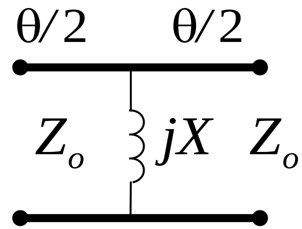
$$K = \frac{1}{\omega C}$$

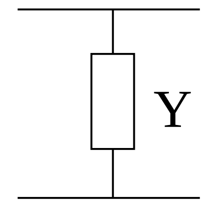


$$J = \omega C$$

(derivation of impedance inverter)







$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} 1 & 0 \\ Y & 1 \end{bmatrix}$$

$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} \cos\beta l & jZ_o \sin\beta l \\ jY_o \sin\beta l & \cos\beta l \end{bmatrix}, \quad \begin{matrix} Z_o = K \;\; \beta l = -\frac{\pi}{2} \\ l = -\frac{\lambda}{4} \end{matrix} \rightarrow \begin{bmatrix} 0 & -jK \\ -\frac{j}{K} & 0 \end{bmatrix}$$

$$\begin{bmatrix} \cos\frac{\theta}{2} & jZ_o \sin\frac{\theta}{2} \\ \frac{j}{Z_o}\sin\frac{\theta}{2} & \cos\frac{\theta}{2} \end{bmatrix} \begin{bmatrix} 1 & 0 \\ \frac{1}{jX} & 1 \end{bmatrix} \begin{bmatrix} \cos\frac{\theta}{2} & jZ_o \sin\frac{\theta}{2} \\ \frac{j}{Z_o}\sin\frac{\theta}{2} & \cos\frac{\theta}{2} \end{bmatrix} = \begin{bmatrix} \cos\theta + \frac{Z_o}{2X}\sin\theta & jZ_o(\sin\theta + \frac{Z_o}{X}\sin^2\frac{\theta}{2}) \\ j(\frac{1}{Z_o}\sin\theta - \frac{1}{X}\cos^2\frac{\theta}{2}) & \cos\theta + \frac{Z_o}{2X}\sin\theta \end{bmatrix}$$

$$\cos\theta + \frac{Z_o}{2X}\sin\theta = 0 \qquad \theta = -\tan^{-1}\frac{2X}{Z_o} \qquad (1)-(2) \rightarrow X = \frac{K}{1-(\frac{K}{Z_o})^2}$$

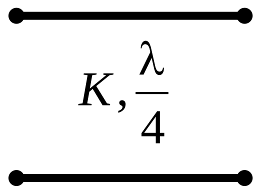
$$\rightarrow j(\frac{1}{Z_o}\sin\theta - \frac{1}{X}\cos^2\frac{\theta}{2}) = -\frac{j}{K} \rightarrow \sin\theta - \frac{Z_o}{X}\cos^2\frac{\theta}{2} = -\frac{Z_o}{K} \ldots(1) \rightarrow$$

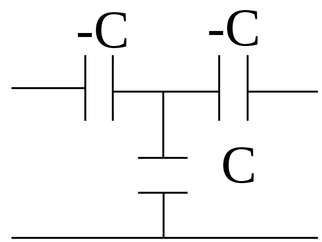
$$jZ_o(\sin\theta + \frac{Z_o}{X}\sin^2\frac{\theta}{2}) = -jK \qquad \sin\theta + \frac{Z_o}{X}\sin^2\frac{\theta}{2} = -\frac{K}{Z_o} \ldots(2)$$

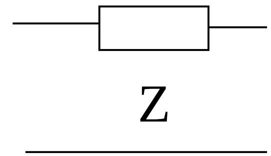
$$\tan|\theta| = \frac{2X}{Z_o} = \frac{2K/Z_o}{1-(\frac{K}{Z_o})^2} = \frac{2\tan\left|\frac{\theta}{2}\right|}{1-\tan^2\left|\frac{\theta}{2}\right|}, \quad K = Z_o \tan\left|\frac{\theta}{2}\right|$$

微波電路講義

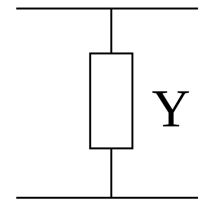
(derivation of impedance inverter)







$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} 1 & Z \\ 0 & 1 \end{bmatrix}$$

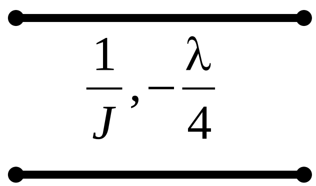


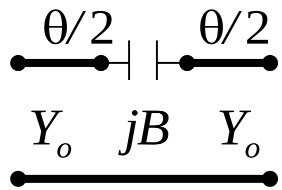
$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} 1 & 0 \\ Y & 1 \end{bmatrix}$$

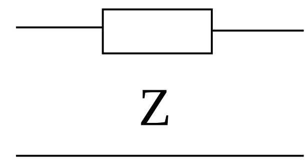
$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} \cos\beta l & jZ_o \sin\beta l \\ jY_o \sin\beta l & \cos\beta l \end{bmatrix}, \quad \begin{matrix} Z_o = K \\ l = \frac{\lambda}{4} \end{matrix} \; \xrightarrow{\beta l = \frac{\pi}{2}} \begin{bmatrix} 0 & jK \\ \frac{j}{K} & 0 \end{bmatrix}$$

$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} 1 & -\frac{1}{j\omega C} \\ 0 & 1 \end{bmatrix} \begin{bmatrix} 1 & 0 \\ j\omega C & 1 \end{bmatrix} \begin{bmatrix} 1 & -\frac{1}{j\omega C} \\ 0 & 1 \end{bmatrix} = \begin{bmatrix} 0 & j\frac{1}{\omega C} \\ j\omega C & 0 \end{bmatrix} \rightarrow K = \frac{1}{\omega C}$$

(derivation of admittance inverter)







$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} 1 & Z \\ 0 & 1 \end{bmatrix}$$

$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} \cos\beta l & jZ_o \sin\beta l \\ jY_o \sin\beta l & \cos\beta l \end{bmatrix}, \begin{matrix} Y_o = J \\ l = -\frac{\lambda}{4} \end{matrix} \xrightarrow{\beta l = -\frac{\pi}{2}} \begin{bmatrix} 0 & -\frac{j}{J} \\ -jJ & 0 \end{bmatrix}$$

$$\begin{bmatrix} \cos\frac{\theta}{2} & \frac{j}{Y_o}\sin\frac{\theta}{2} \\ jY_o \sin\frac{\theta}{2} & \cos\frac{\theta}{2} \end{bmatrix} \begin{bmatrix} 1 & \frac{1}{jB} \\ 0 & 1 \end{bmatrix} \begin{bmatrix} \cos\frac{\theta}{2} & \frac{j}{Y_o}\sin\frac{\theta}{2} \\ jY_o \sin\frac{\theta}{2} & \cos\frac{\theta}{2} \end{bmatrix} = \begin{bmatrix} \cos\theta + \frac{Y_o}{2B}\sin\theta & j(\frac{1}{Y_o}\sin\theta - \frac{1}{B}\cos^2\frac{\theta}{2}) \\ jY_o(\sin\theta + \frac{Y_o}{B}\sin^2\frac{\theta}{2}) & \cos\theta + \frac{Y_o}{2B}\sin\theta \end{bmatrix}$$

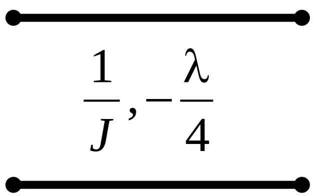
$$\cos\theta + \frac{Y_o}{2B}\sin\theta = 0 \qquad \theta = -\tan^{-1}\frac{2B}{Y_o} \qquad (1)-(2) \rightarrow B = \frac{J}{1-(\frac{J}{Y_o})^2}$$

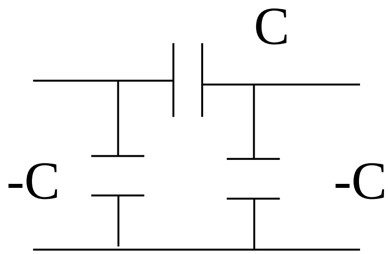
$$\rightarrow j(\frac{1}{Y_o}\sin\theta - \frac{1}{B}\cos^2\frac{\theta}{2}) = -\frac{j}{J} \rightarrow \sin\theta - \frac{Y_o}{B}\cos^2\frac{\theta}{2} = -\frac{Y_o}{J} \ldots(1) \rightarrow$$

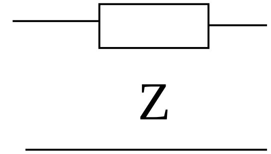
$$jY_o(\sin\theta + \frac{Y_o}{B}\sin^2\frac{\theta}{2}) = -jJ \qquad \sin\theta + \frac{Y_o}{B}\sin^2\frac{\theta}{2} = -\frac{J}{Y_o} \ldots(2)$$

$$\tan|\theta| = \frac{2B}{Y_o} = \frac{2J/Y_o}{1-(\frac{J}{Y_o})^2} = \frac{2\tan\left|\frac{\theta}{2}\right|}{1-\tan^2\left|\frac{\theta}{2}\right|}, J = Y_o \tan\left|\frac{\theta}{2}\right|$$

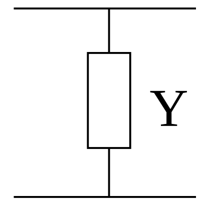
(derivation of admittance inverter)







$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} 1 & Z \\ 0 & 1 \end{bmatrix}$$



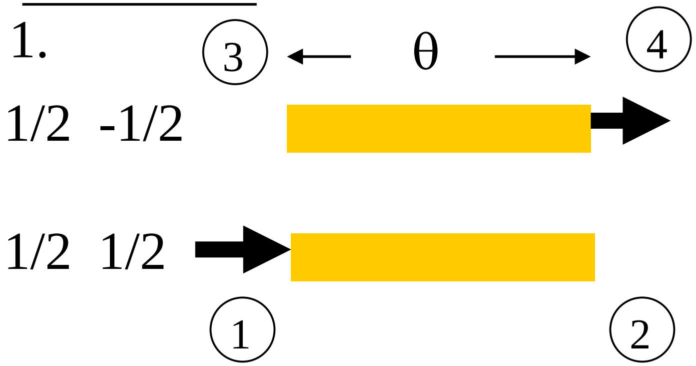
$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} 1 & 0 \\ Y & 1 \end{bmatrix}$$

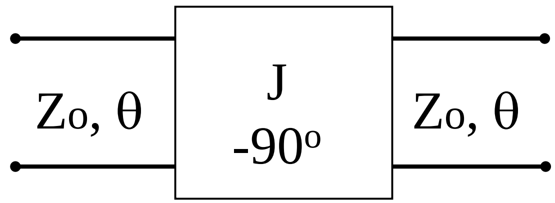
$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} \cos\beta l & jZ_o \sin\beta l \\ jY_o \sin\beta l & \cos\beta l \end{bmatrix}, \begin{matrix} Y_o = J \\ l = -\frac{\lambda}{4} \end{matrix} \xrightarrow{\beta l = -\frac{\pi}{2}} \begin{bmatrix} 0 & \frac{1}{jJ} \\ -jJ & 0 \end{bmatrix}$$

$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} 1 & 0 \\ -j\omega C & 1 \end{bmatrix} \begin{bmatrix} 1 & \frac{1}{j\omega C} \\ 0 & 1 \end{bmatrix} \begin{bmatrix} 1 & 0 \\ -j\omega C & 1 \end{bmatrix} = \begin{bmatrix} 0 & \frac{1}{j\omega C} \\ -j\omega C & 0 \end{bmatrix} \rightarrow J = \omega C$$

Discussion

1.





design equation #1

$$\theta = \frac{\pi}{2}, \begin{cases} Z_{oe} = Z_o[1 + JZ_o + (JZ_o)^2] \\ Z_{oo} = Z_o[1 - JZ_o + (JZ_o)^2] \end{cases}$$

For the left circuit: $V_1 = V_{1e}^+ + V_{1e}^- + V_{1o}^+ + V_{1o}^-, I_1 = \frac{V_{1e}^+}{Z_{oe}} - \frac{V_{1e}^-}{Z_{oe}} + \frac{V_{1o}^+}{Z_{oo}} - \frac{V_{1o}^-}{Z_{oo}}$

$$V_2 = V_{1e}^+ e^{-j\theta} + V_{1e}^- e^{j\theta} + V_{1o}^+ e^{-j\theta} + V_{1o}^- e^{j\theta}, I_2 = \frac{V_{1e}^+}{Z_{oe}} e^{-j\theta} - \frac{V_{1e}^-}{Z_{oe}} e^{j\theta} + \frac{V_{1o}^+}{Z_{oo}} e^{-j\theta} - \frac{V_{1o}^-}{Z_{oo}} e^{j\theta}$$

$$V_3 = V_{1e}^+ + V_{1e}^- - V_{1o}^+ - V_{1o}^-, I_3 = \frac{V_{1e}^+}{Z_{oe}} - \frac{V_{1e}^-}{Z_{oe}} - \frac{V_{1o}^+}{Z_{oo}} + \frac{V_{1o}^-}{Z_{oo}}$$

$$V_4 = V_{1e}^+ e^{-j\theta} + V_{1e}^- e^{j\theta} - V_{1o}^+ e^{-j\theta} - V_{1o}^- e^{j\theta}, I_4 = \frac{V_{1e}^+}{Z_{oe}} e^{-j\theta} - \frac{V_{1e}^-}{Z_{oe}} e^{j\theta} - \frac{V_{1o}^+}{Z_{oo}} e^{-j\theta} + \frac{V_{1o}^-}{Z_{oo}} e^{j\theta}$$

$$\begin{bmatrix} V_1 \\ V_4 \end{bmatrix} = \begin{bmatrix} Z_{11} & Z_{14} \\ Z_{14} & Z_{11} \end{bmatrix} \begin{bmatrix} I_1 \\ I_4 \end{bmatrix}, Z_{11} = \left.\frac{V_1}{I_1}\right|_{I_4=0}, Z_{14} = \left.\frac{V_4}{I_1}\right|_{I_4=0}$$

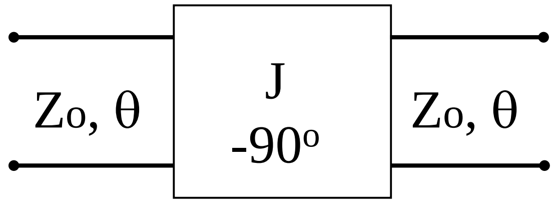
$$V_{1o}^- = V_{1o}^+ e^{-j2\theta}$$

ports 2, 3 open, $I_2 = I_3 = 0$

$I_4 = 0$

$$\Rightarrow \frac{V_{1e}^+}{Z_{oe}} = \frac{V_{1o}^+}{Z_{oo}} \qquad \frac{V_{1e}^-}{Z_{oe}} = \frac{V_{1o}^+}{Z_{oo}} \Rightarrow \begin{aligned} Z_{11} &= -\frac{j}{2}(Z_{oe} + Z_{oo})\cot\theta \\ Z_{14} &= -\frac{j}{2}(Z_{oe} - Z_{oo})\csc\theta \end{aligned}$$

$$\begin{bmatrix} A & B \\ C & D \end{bmatrix} = \begin{bmatrix} \dfrac{Z_{11}}{Z_{41}} & \dfrac{Z_{11}Z_{44}}{Z_{41}} - Z_{14} \\ \dfrac{1}{Z_{41}} & \dfrac{Z_{44}}{Z_{41}} \end{bmatrix} = \begin{bmatrix} \dfrac{Z_{oe} + Z_{oo}}{Z_{oe} - Z_{oo}}\cos\theta & 2j\dfrac{(Z_{oe} - Z_{oo})^2 - (Z_{oe} + Z_{oo})^2\cos\theta}{(Z_{oe} - Z_{oo})\sin\theta} \\ 2j\dfrac{\sin\theta}{Z_{oe} - Z_{oo}} & \dfrac{Z_{oe} + Z_{oo}}{Z_{oe} - Z_{oo}}\cos\theta \end{bmatrix}$$



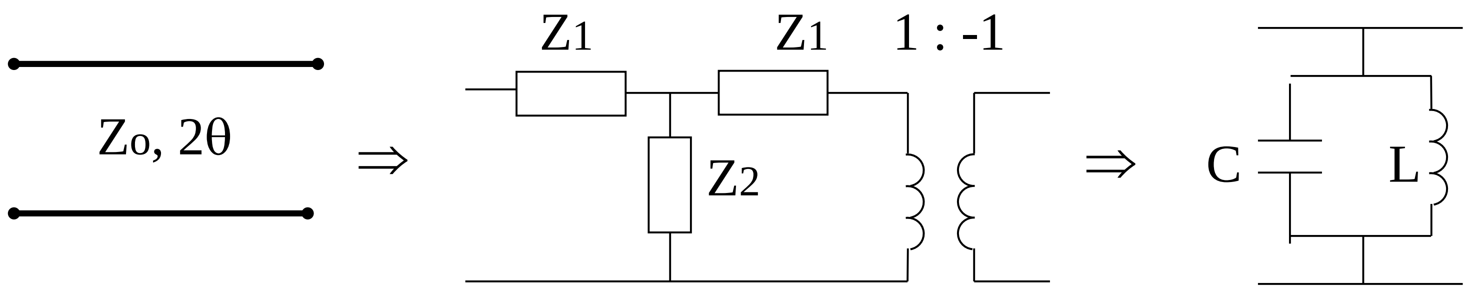
$$\begin{bmatrix} \cos\theta & jZ_o\sin\theta \\ jY_o\sin\theta & \cos\theta \end{bmatrix}\begin{bmatrix} 0 & -\frac{j}{J} \\ -jJ & 0 \end{bmatrix}\begin{bmatrix} \cos\theta & jZ_o\sin\theta \\ jY_o\sin\theta & \cos\theta \end{bmatrix}$$

$$= \begin{bmatrix} (Z_oJ+\frac{Y_o}{J})\sin\theta\cos\theta & jZ_o^2J\sin^2\theta-\frac{j}{J}\cos^2\theta \\ -jJ\cos^2\theta+j\frac{Y_o^2}{J}\sin^2\theta & (Z_oJ+\frac{Y_o}{J})\sin\theta\cos\theta \end{bmatrix}$$

$$"=" \Rightarrow (Z_oJ+\frac{Y_o}{J})\sin\theta\cos\theta = \frac{Z_{oe}+Z_{oo}}{Z_{oe}-Z_{oo}}\cos\theta, -jJ\cos^2\theta+j\frac{Y_o^2}{J}\sin^2\theta = \frac{j2\sin\theta}{Z_{oe}-Z_{oo}}$$

$$\theta=\frac{\pi}{2} \Rightarrow \frac{Z_{oe}+Z_{oo}}{Z_{oe}-Z_{oo}} = Z_oJ+\frac{Y_o}{J}, Z_{oe}-Z_{oo} = 2\frac{J}{Y_o^2} = 2JZ_o^2$$

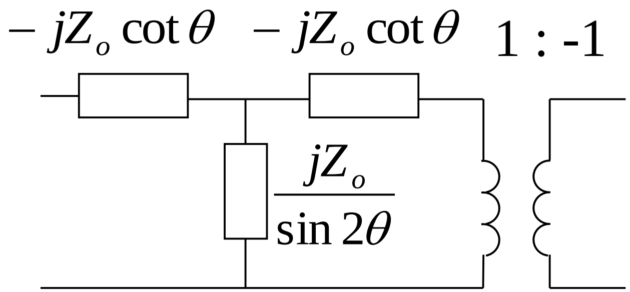
$$\Rightarrow \begin{matrix} Z_{oe} = Z_o(1+JZ_o+J^2Z_o^2) \\ Z_{oo} = Z_o(1-JZ_o-J^2Z_o^2) \end{matrix}$$

2. 

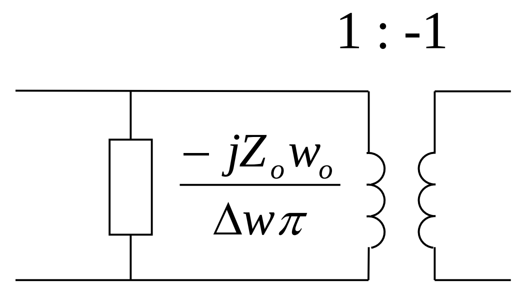
design equation #2 $L = \dfrac{2Z_o}{\omega_o \pi}, C = \dfrac{\pi}{2\omega_o Z_o}$

$$\begin{bmatrix} \cos 2\theta & jZ_o \sin 2\theta \\ jY_o \sin 2\theta & \cos 2\theta \end{bmatrix} = \begin{bmatrix} 1+\dfrac{Z_1}{Z_2} & 2Z_1+\dfrac{Z_1^2}{Z_2} \\ \dfrac{1}{Z_2} & 1+\dfrac{Z_1}{Z_2} \end{bmatrix} \begin{bmatrix} -1 & 0 \\ 0 & -1 \end{bmatrix} = -\begin{bmatrix} 1+\dfrac{Z_1}{Z_2} & 2Z_1+\dfrac{Z_1^2}{Z_2} \\ \dfrac{1}{Z_2} & 1+\dfrac{Z_1}{Z_2} \end{bmatrix}$$

$$\Rightarrow \begin{array}{c} Z_2 = \dfrac{jZ_o}{\sin 2\theta} \\ -(1+\dfrac{Z_1}{Z_2}) = \cos 2\theta \end{array} \Rightarrow \begin{array}{c} Z_2 = \dfrac{jZ_o}{\sin 2\theta} \\ Z_1 = -jZ_o \cot\theta \end{array}$$

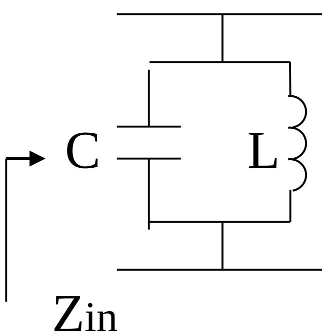


$\Rightarrow$



$$\text{for } \theta \approx \frac{\pi}{2},\ \cot\theta \approx 0$$

$$2\theta = \beta l = \frac{w}{c} l = \frac{w_o + \Delta w}{w_o}\pi \to \sin 2\theta = \sin(\pi + \frac{\Delta w}{w_o}\pi) = -\sin\frac{\Delta w}{w_o}\pi \approx -\frac{\Delta w}{w_o}\pi$$



$$Z_{in} = \frac{1}{jwC + \dfrac{1}{jwL}} = \frac{jwL}{1 - w^2 LC} = \frac{j(w_o + \Delta w)L}{1 - (w_o + \Delta w)^2 LC}$$

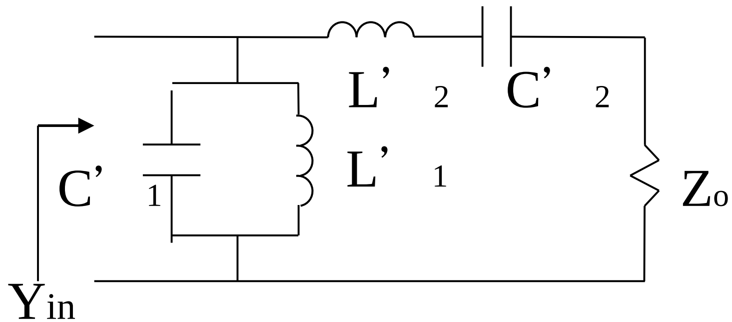
$$= \frac{-j(w_o + \Delta w)L}{(2w_o \Delta w + \Delta w^2)\dfrac{1}{w_o^2}} \approx \frac{-jw_o(w_o + \Delta w)L}{2\Delta w} \approx \frac{-jw_o^2}{2\Delta w} L$$

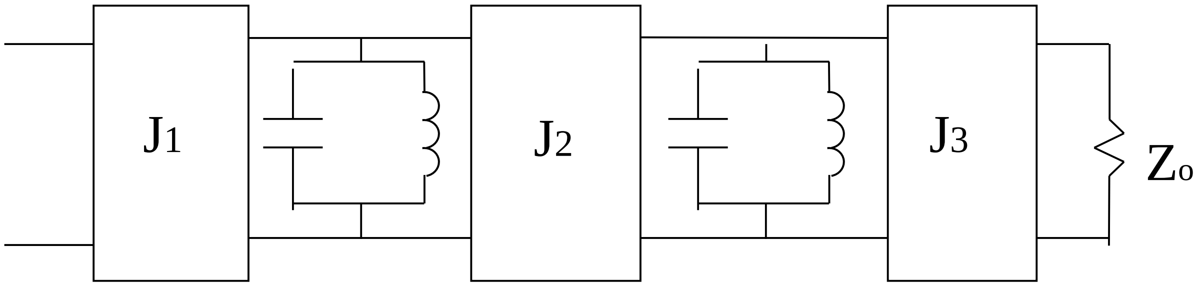
$$\text{"="} \Rightarrow \frac{-jw_o^2}{2\Delta w} L = \frac{-jw_o Z_o}{\Delta w \pi} \Rightarrow L = \frac{2Z_o}{w_o \pi}, C = \frac{1}{Lw_o^2} = \frac{\pi}{2w_o Z_o}$$

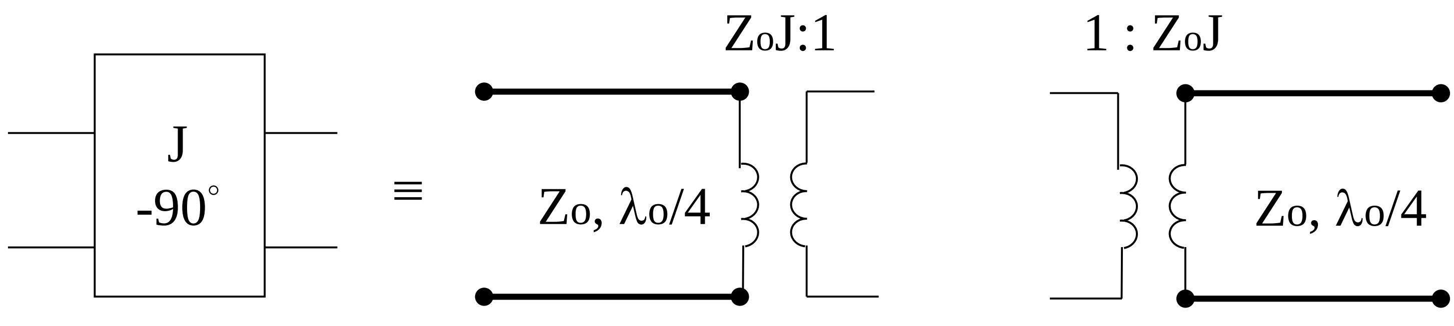
3. derivation of design equation #3 (8.121)

$$J_1 = \frac{1}{Z_o}\sqrt{\frac{\pi\Delta}{2g_1}},\ J_i = \frac{\pi\Delta}{2Z_o\sqrt{g_{i-1}g_i}},\ J_{N+1} = \frac{1}{Z_o}\sqrt{\frac{\pi\Delta}{2g_N g_{N+1}}}$$

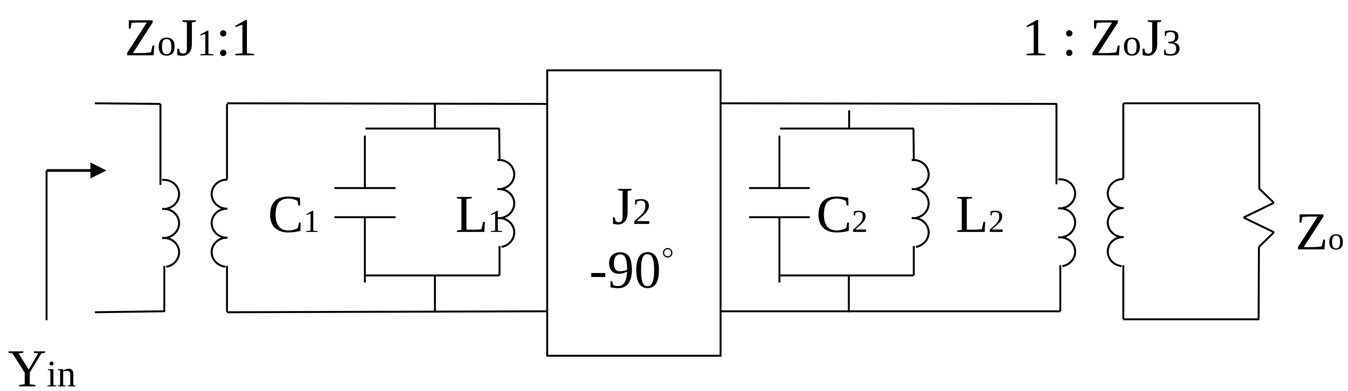
"N=2" (p.434-435, Fig. 8.45 (e), (f))



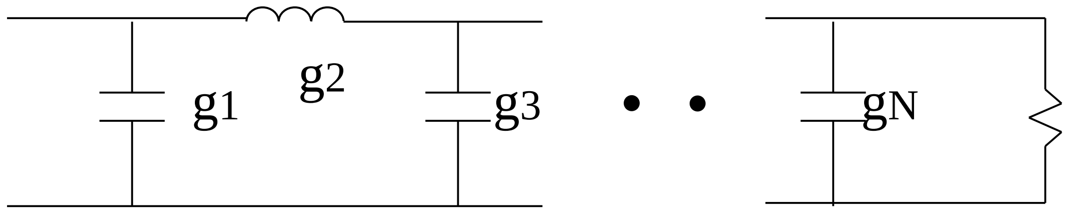


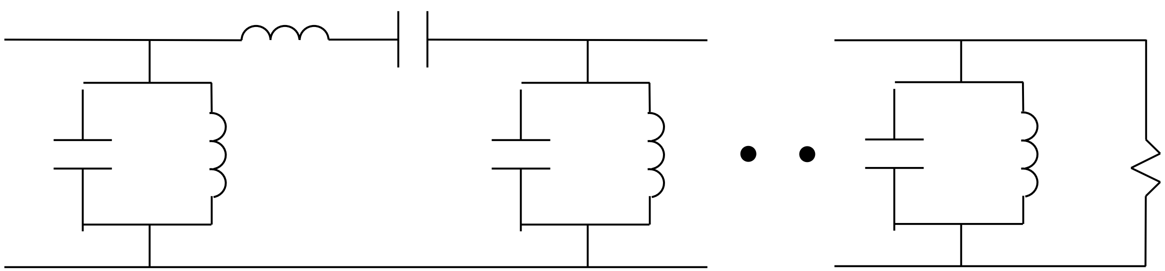


$$\text{left}:\begin{bmatrix} 0 & \frac{-j}{J} \\ -jJ & 0 \end{bmatrix} = \text{right}:\begin{bmatrix} 0 & -jZ_o \\ -jY_o & 0 \end{bmatrix}\begin{bmatrix} JZ_o & 0 \\ 0 & \frac{1}{JZ_o} \end{bmatrix},\begin{bmatrix} \frac{1}{JZ_o} & 0 \\ 0 & JZ_o \end{bmatrix}\begin{bmatrix} 0 & -jZ_o \\ -jY_o & 0 \end{bmatrix}$$

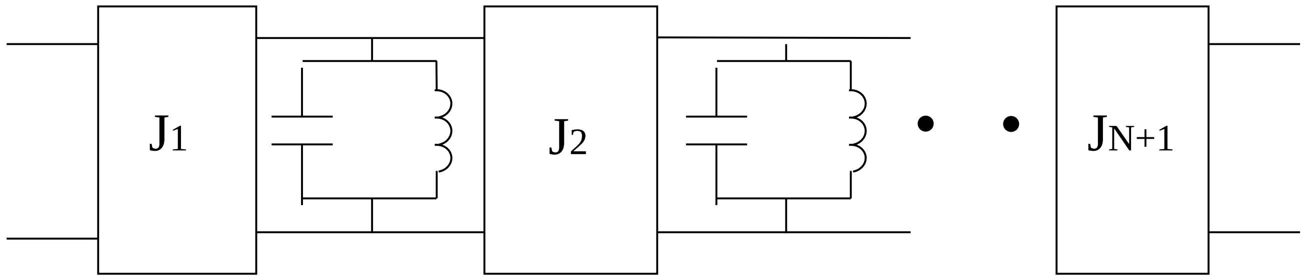


4. Coupled line BPF design

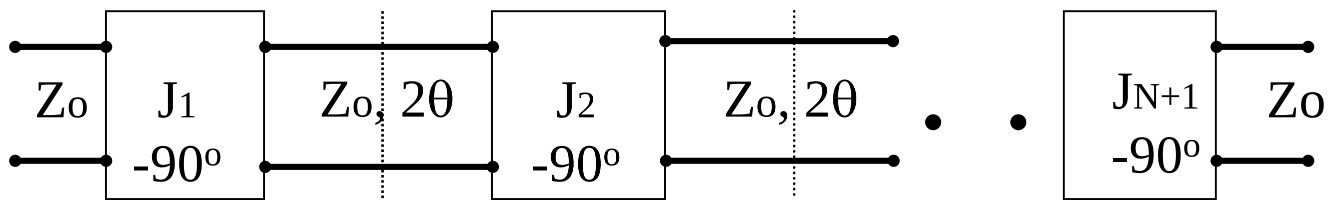




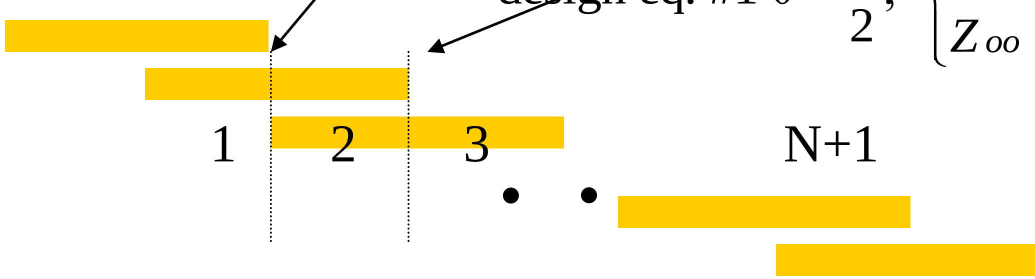
$$L_i = \begin{cases} \dfrac{\Delta Z_o}{\omega_o g_i} & \text{shunt element} \\ \dfrac{g_i Z_o}{\omega_o \Delta} & \text{series element} \end{cases},\ C_i = \begin{cases} \dfrac{g_i}{\omega_o \Delta Z_o} & \text{shunt element} \\ \dfrac{\Delta}{\omega_o g_i Z_o} & \text{series element} \end{cases},\ \Delta = \frac{\omega_2 - \omega_1}{\omega_o}$$



design equation #3 $J_1 = \dfrac{1}{Z_o}\sqrt{\dfrac{\pi\Delta}{2g_1}},\ J_i = \dfrac{\pi\Delta}{2Z_o\sqrt{g_{i-1}g_i}},\ J_{N+1} = \dfrac{1}{Z_o}\sqrt{\dfrac{\pi\Delta}{2g_N g_{N+1}}}$



design eq. #1 $\theta = \dfrac{\pi}{2},\ \begin{cases} Z_{oe} = Z_o[1 + JZ_o + (JZ_o)^2] \\ Z_{oo} = Z_o[1 - JZ_o + (JZ_o)^2] \end{cases}$



4. Microstrp coupled line BPF design procedure
LPF prototype gi $\rightarrow$ Ji $\rightarrow$ Zoei, Zooi $\rightarrow$ microstrip line Wi, Si
$\rightarrow$ consider discontunuity effects

$$J_1 = \frac{1}{Z_o}\sqrt{\frac{\pi\Delta}{2g_1}}, J_i = \frac{\pi\Delta}{2Z_o\sqrt{g_{i-1}g_i}}, J_{N+1} = \frac{1}{Z_o}\sqrt{\frac{\pi\Delta}{2g_N g_{N+1}}}$$

$$Z_{oe} = Z_o[1 + JZ_o + (JZ_o)^2], Z_{oo} = Z_o[1 - JZ_o + (JZ_o)^2]$$

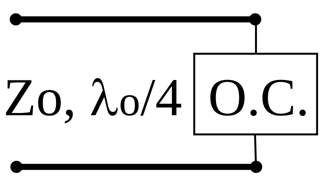
5. Ex.8.7 design a 0.5dB ripple equal-ripple coupled line BPF, N=3, f_o=2GHz, BW=10%, Z_o=50Ω

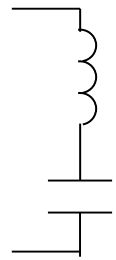
i	g_i	Z_oJ_i	Z_{oe}	Z_{oo}
1	1.5963	0.3137	70.61	39.24
2	1.0967	0.1187	56.64	44.77
3	1.5963	0.1187	56.64	44.77
4	1.0000	0.3137	70.61	39.24

frequency response
(p.436, Fig.8.46)
IL(1.8GHz) ≅ 20dB

8.8 Filters using coupled resonators

• λ/4 stub





design equation

$$L=\frac{\pi Z_o}{4\omega_o}, C=\frac{4}{\omega_o \pi Z_o}$$

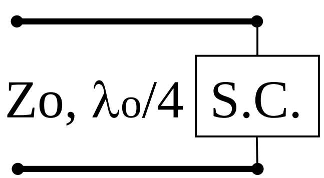
O.C. line: $Z_{in}=\frac{Z_o}{j\tan\theta}, \theta=\beta l=\frac{w}{c}\frac{\lambda_o}{4}=\frac{w}{c}\frac{c}{4f_o}=\frac{\pi}{2}\frac{w}{w_o}=\frac{\pi}{2}\frac{w_o+\Delta w}{w_o}$

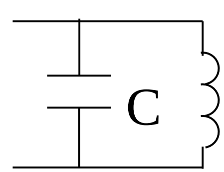
$$Z_{in}=\frac{Z_o}{j\tan(\frac{\pi}{2}+\frac{\pi}{2}\frac{\Delta w}{w_o})}=jZ_o\tan\frac{\pi\Delta w}{2w_o}\approx jZ_o\frac{\pi(w-w_o)}{2w_o}$$

series LC: $Z_{in}=jwL+\frac{1}{jwC}=j\sqrt{\frac{L}{C}}(w\sqrt{LC}-\frac{1}{w\sqrt{LC}})=j\sqrt{\frac{L}{C}}(\frac{w}{w_o}-\frac{w_o}{w})$

$$=j\sqrt{\frac{L}{C}}\frac{(w+w_o)(w-w_o)}{w_o w}\approx j\sqrt{\frac{L}{C}}\frac{2(w-w_o)}{w_o}=j2L(w-w_o)\Rightarrow Z_o=\frac{4w_oL}{\pi}$$

design equation

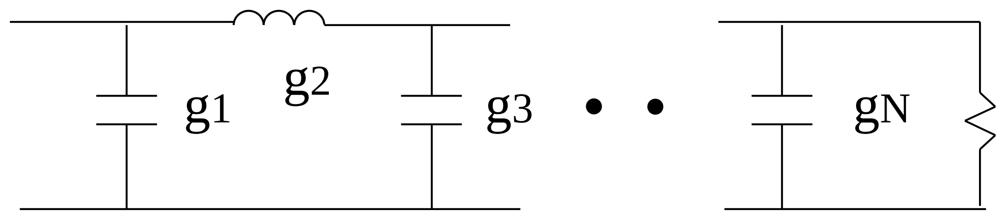


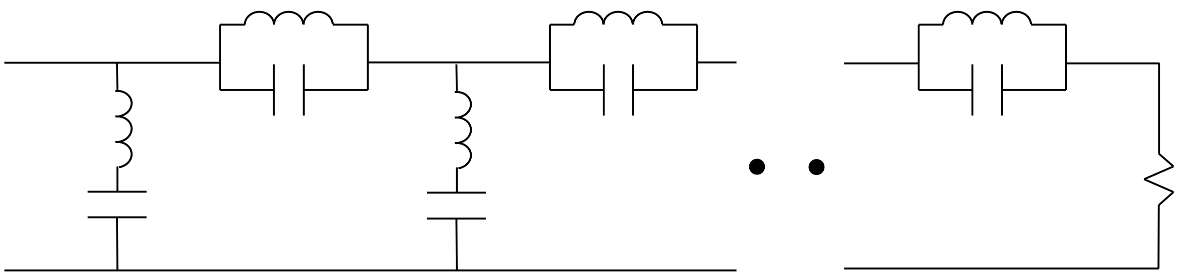


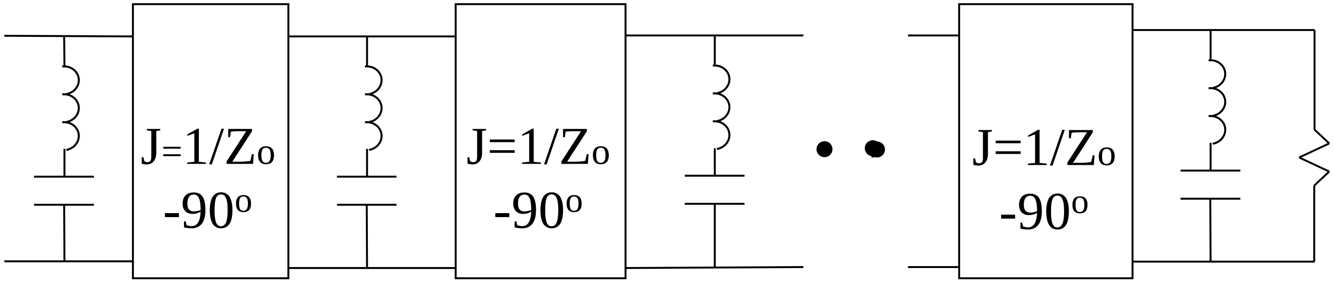
$$C=\frac{\pi Z_o}{4\omega_o},\ L=\frac{4}{\omega_o\pi Z_o}$$

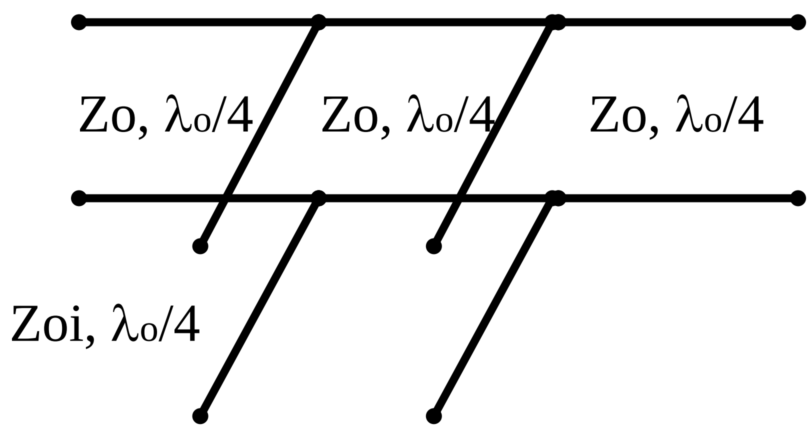
Discussion

1. BSF using $\lambda/4$ open-circuit stub









design equation BSF: $\frac{\lambda}{4}$ open-circuit shunt stub $Z_{oi} = \frac{4Z_o}{\pi g_i \Delta}$

(BPF: $\frac{\lambda}{4}$ short-circuit shunt stub $Z_{oi} = \frac{\pi Z_o \Delta}{4g_i}$)

Derivation for N=2 is given in p.439-440.

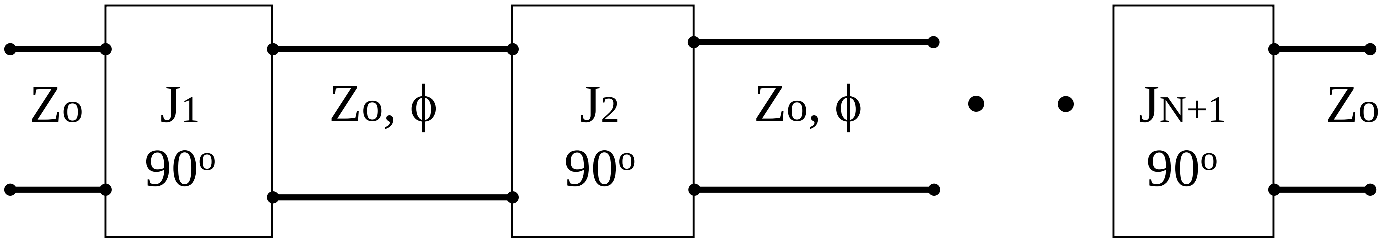
2. Ex.8.8 design a 0.5dB ripple equal-ripple $\lambda/4$ stub BSF, $N=3$, $f_o=2GHz$, $BW=15\%$, $Z_o=50\Omega$

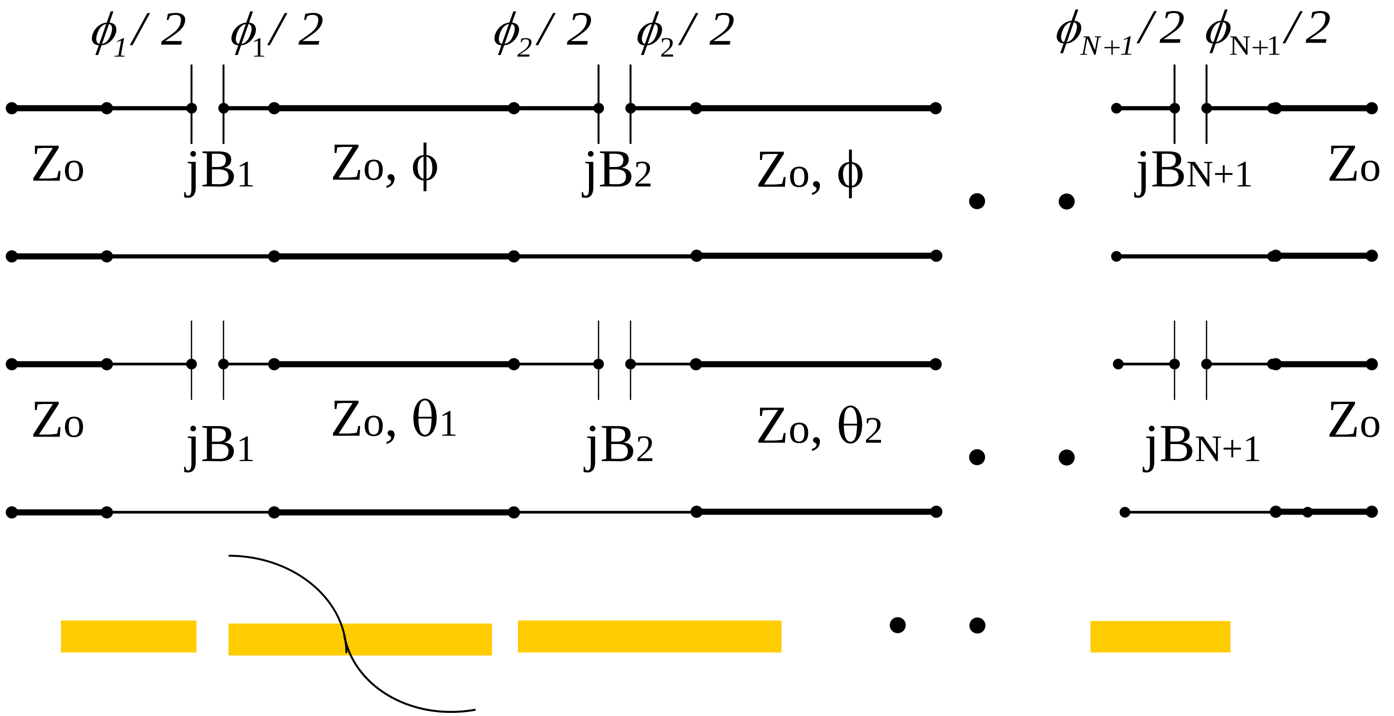
i	g_i	Z_{oi}
1	1.5963	265.9
2	1.0967	387
3	1.5963	265.9

frequency response (p.440, Fig.8.49)

3. Design procedure for microstrip BPF or BSF using $\lambda/4$ stub
LPF prototype g_i $\rightarrow$ $\lambda/4$ open-circuit or short-circui stubs Z_{oi}
$\rightarrow$ microstrip line $\rightarrow$ consider discontunuity effect

4. BPF using capacitively coupled series resonator





design equation

$$\phi_o = \pi\ (l = \frac{\lambda_o}{2}),\ \theta_i = \pi + \frac{\phi_i}{2} + \frac{\phi_{i+1}}{2} = \pi - (\tan^{-1}\frac{2B_i}{Y_o} + \tan^{-1}\frac{2B_{i+1}}{Y_o})$$

$$B_i = \frac{J_i}{1-(Z_o J_i)^2}$$

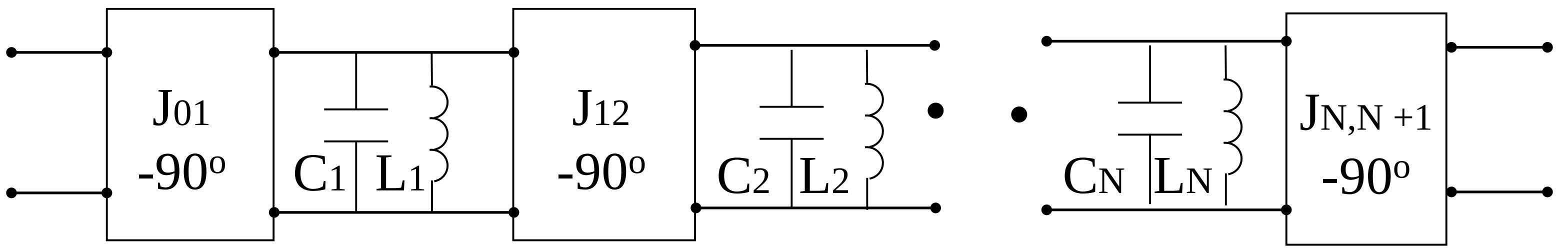
5. Design procedure for microstrip BPF using capacitively coupled resonator
LPF prototype g_i → J_i → B_i, ϕ_i → C_i, θ_i → microstrip gap width and line length → consider discontunuity effect

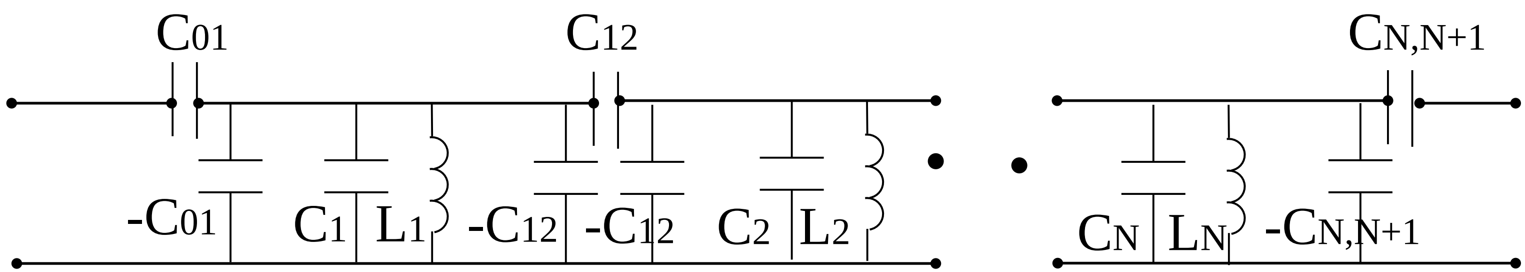
6. Ex.8.9 design a 0.5dB ripple equal-ripple BPF using capacitively coupled resonators, f_o=2GHz, BW=10%, Z_o=50Ω, IL(2.2GHz) > 20dB

i	g_i	Z_oJ_i	$B_i(x10^{-3})$	C_i(pF)	θ_i(deg)
1	1.5963	0.3137	6.96	0.554	155.8
2	1.0967	0.1187	2.41	0.192	166.5
3	1.5963	0.1187	2.41	0.192	166.5
4	1.0000	0.3137	6.96	0.554	

frequency response (p.443, Fig.8.51)

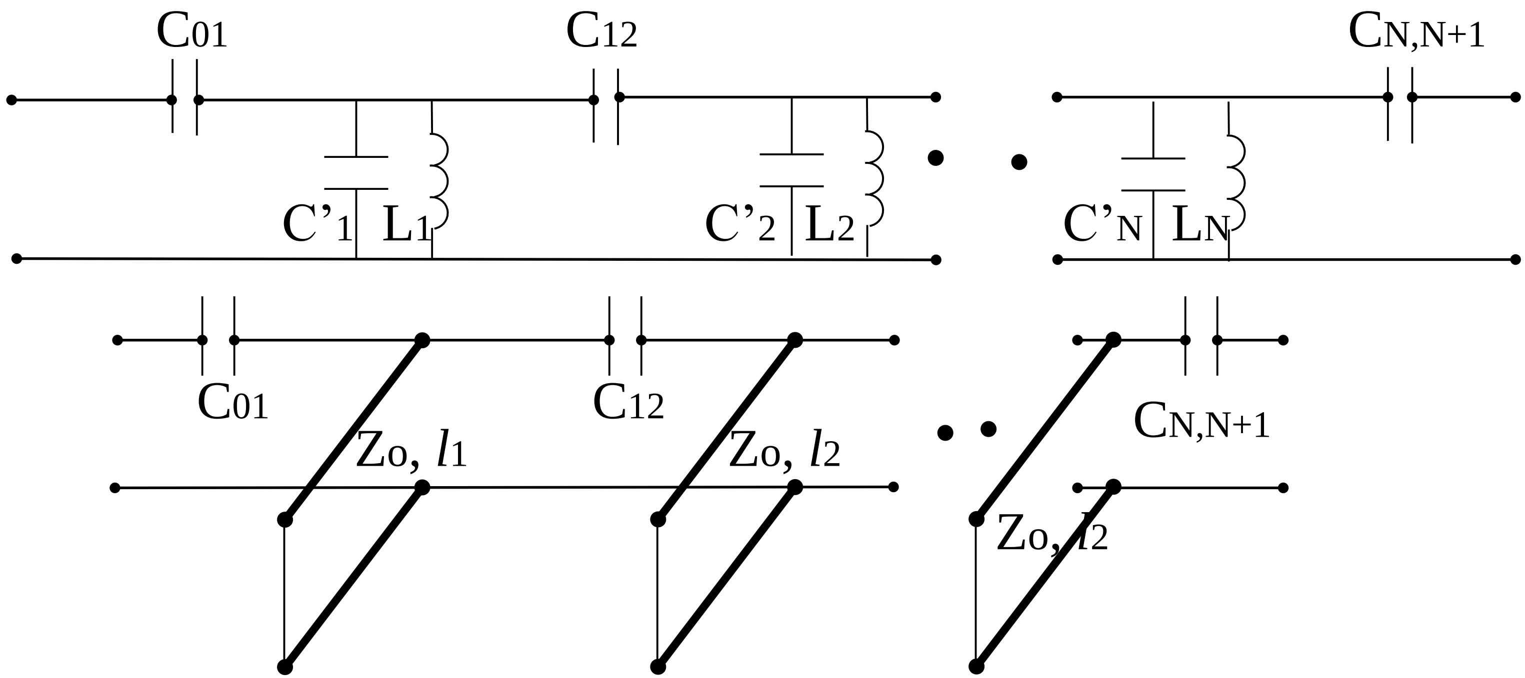
7. BPF using capacitively coupled shunt stub resonator





design equation $Z_o J_{01} = \sqrt{\dfrac{\pi\Delta}{4g_1}}, Z_o J_{n,n+1} = \dfrac{\pi\Delta}{4\sqrt{g_n g_{n+1}}}, Z_o J_{N,N+1} = \sqrt{\dfrac{\pi\Delta}{4g_N g_{N+1}}}$

$$C_{01} = \frac{J_{01}}{w_0\sqrt{1-(Z_0 J_{01})^2}}, C_{n,n+1} = \frac{J_{n,n+1}}{w_0}, C_{N,N+1} = \frac{J_{N,N+1}}{w_0\sqrt{1-(Z_0 J_{N,N+1})^2}}$$

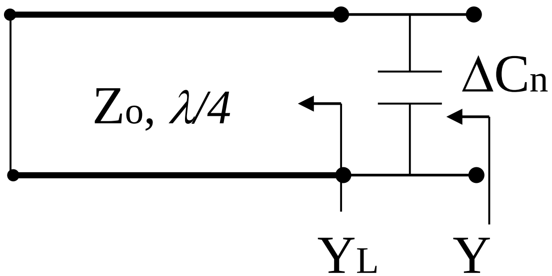


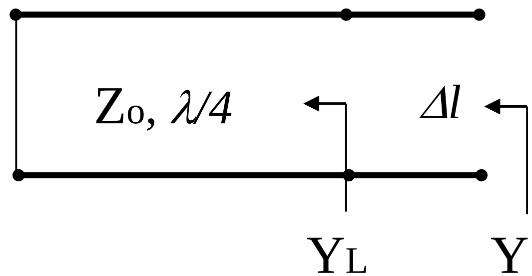
design equation

$$C_n^{'} = C_n - C_{n-1,n} - C_{n,n+1} = C_n + \Delta C_n,\ \Delta C_n = -C_{n-1,n} - C_{n,n+1}$$

$$l_n = \frac{\lambda}{4} + \frac{Z_o w_o \Delta C_n}{2\pi}\lambda$$

(derivation of the change of stub length due to a shunt capacitor)





$$Y = Y_L + jw_o \Delta C_n$$

$$Y = \frac{1}{Z} = \frac{1}{Z_o \dfrac{Z_L + jZ_o \tan\beta\Delta l}{Z_o + jZ_L \tan\beta\Delta l}} = \frac{1}{Z_o} \frac{Z_o + jZ_L \tan\beta\Delta l}{Z_L + jZ_o \tan\beta\Delta l}$$

$$= \frac{1}{Z_o} \frac{Y_L + j\dfrac{1}{Z_o}\tan\beta\Delta l}{\dfrac{1}{Z_o} + jY_L \tan\beta\Delta l} \overset{\beta\Delta l << 1}{\approx} Y_L + j\frac{\beta\Delta l}{Z_o}$$

$$jw_o\Delta C_n = j\frac{\beta_o \Delta l}{Z_o} = j\frac{2\pi\Delta l}{Z_o\lambda} \rightarrow \Delta l = \frac{Z_o w_o \Delta C_n}{2\pi}\lambda$$

8. Design procedure for BPF using capacitively coupled shunt stub resonator

LPF prototype $g_i \rightarrow J_{i-1,i} \rightarrow C_i \rightarrow \Delta C_i \rightarrow \Delta l_i \rightarrow$ resonator length $\rightarrow$ consider discontunuity effect

9. Ex.8.10 design a 0.5dB ripple 3rd order equal-ripple BPF using capacitively coupled shunt resonators, f_o=2GHz, BW=10%, Z_o=50Ω,

i	g_i	$Z_oJ_{i-1,i}$	$C_{i-1,i}$(pF)	ΔC_i(pF)	$\Delta l_i(\lambda)$	l
1	1.5963	0.2218	0.2896	-0.3652	-0.04565	73.6°
2	1.0967	0.0594	0.0756	-0.1512	-0.0189	83.2°
3	1.5963	0.0594	0.0756	-0.3652	-0.04565	73.6°
4	1.0000	0.2218	0.2896			

frequency response (p.447, Fig.8.54)

ADS examples: Ch8_prj